Power Supply Design Seminar

Switch-mode power converter compensation made easy

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Texas Instruments

Switch-mode power converter compensation made easy

Louis Diana

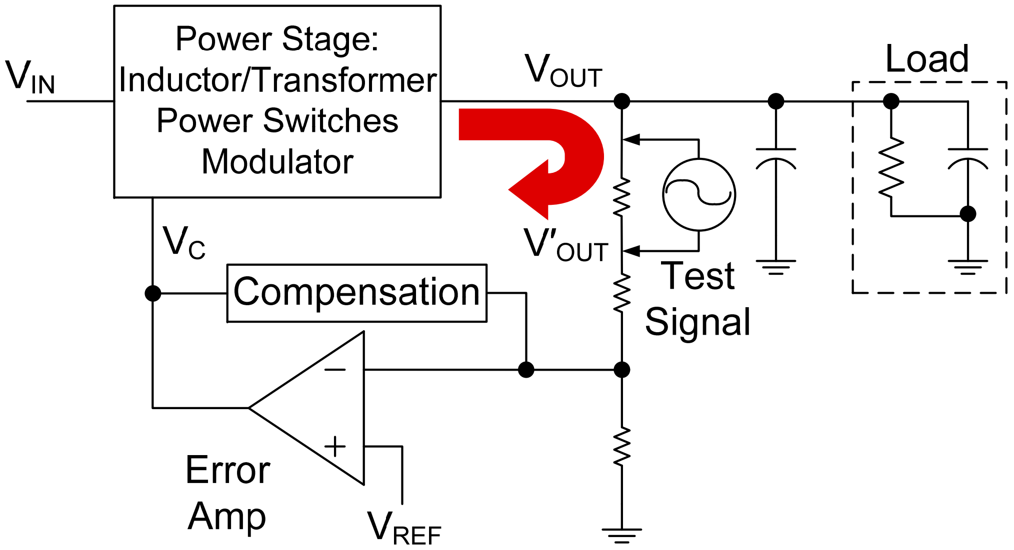
Robert Sheehan

Agenda

- Compensation design and objectives
- Explanation of poles and zeros
- Power stage characteristics
- Error amplifier and transconductance amplifier
- Isolated feedback with optocoupler
- Compensation examples
- Circuit limitations and other issues

Compensation design and objectives

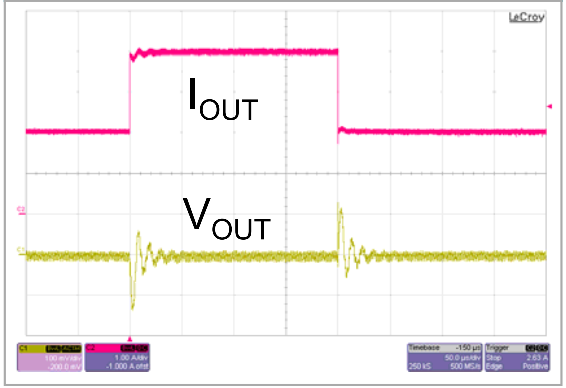
Why do we need feedback and why do we need compensation?



- Feedback is needed to regulate the output voltage
- The bandwidth of the control loop determines the response time

Control loop response

Poor transient response

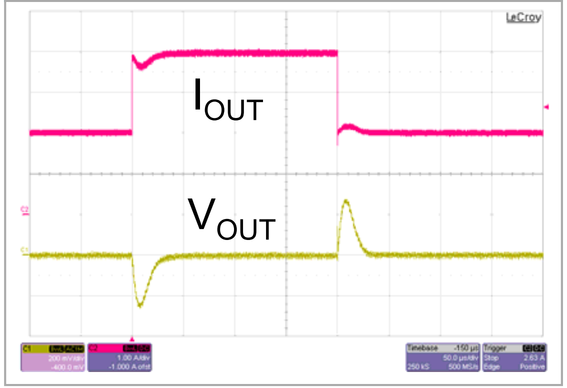


- Response is under-damped causing oscillatory behavior

Objective

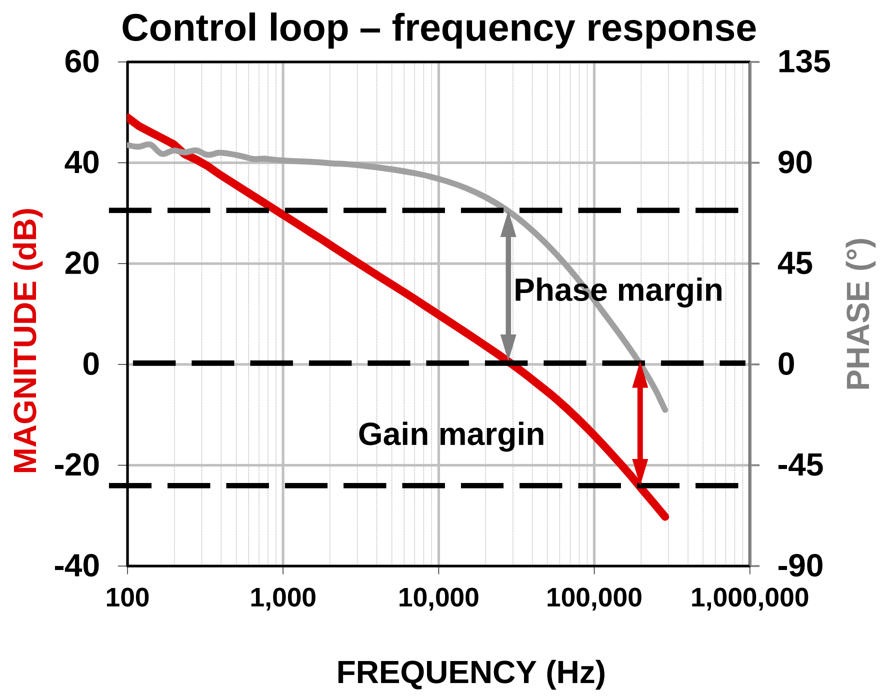
- Maximize crossover frequency for fastest transient response
- Adjust compensation for best settling behavior

Good transient response



- Response is well damped with good settling behavior

Phase margin and gain margin

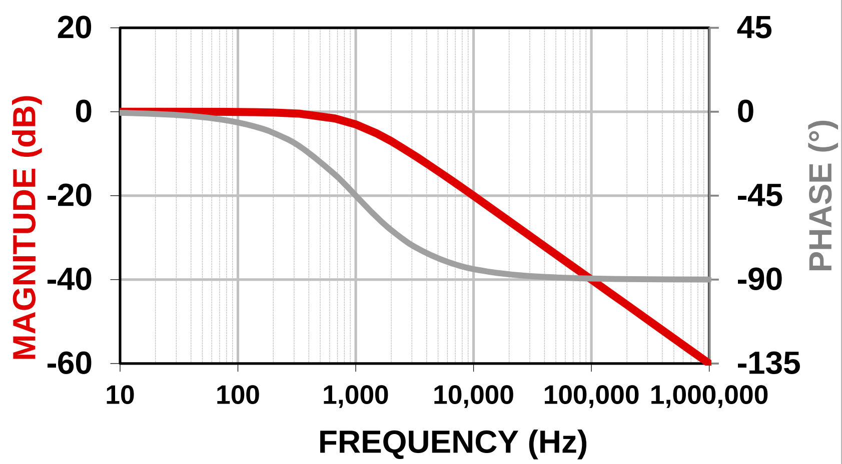


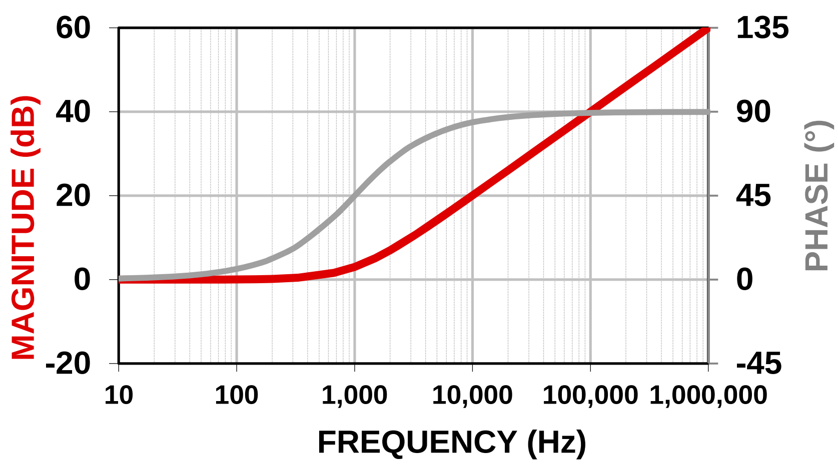
Phase margin and stability

- Sufficient phase margin is needed to prevent oscillation (45º min.)
- Gain margin goal 10 dB min.
- Slope of –20 dB/decade when passing through 0 dB
- Bandwidth rule of thumb is 1/5 to 1/10 of switching frequency

Poles and zeros

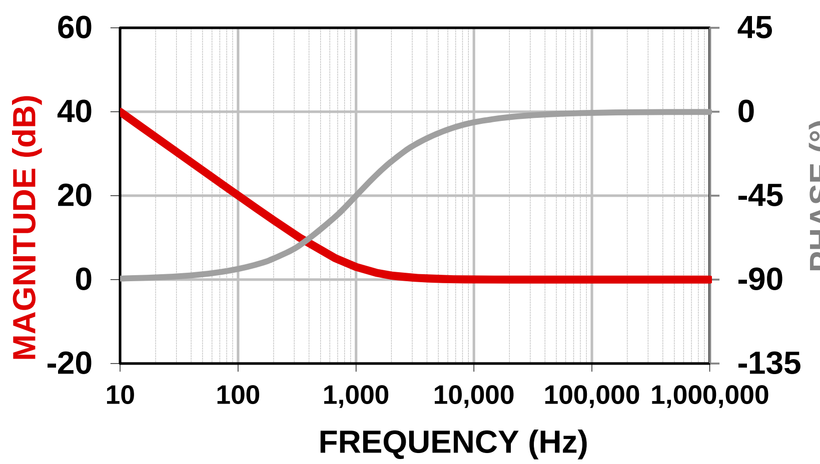
Pole	Zero
$H(s)=\frac{1}{1+\frac{s}{\omega_P}}$	$H(s)=\frac{1+\frac{s}{\omega_Z}}{1}$

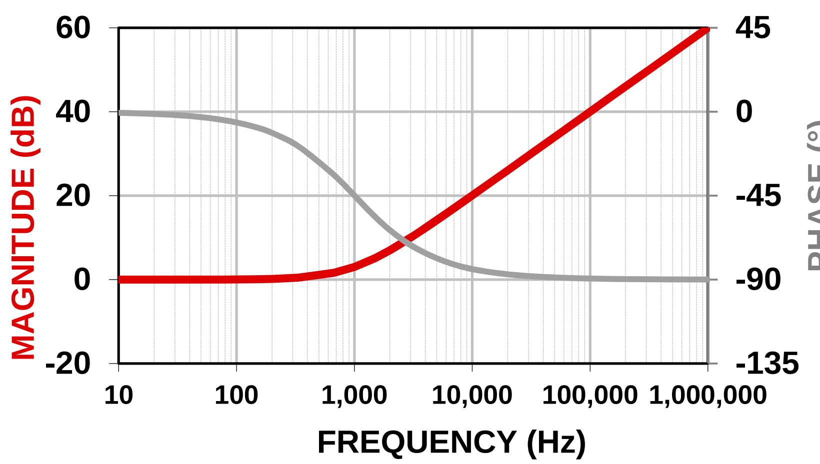




Inverted and right-half-plane zeros

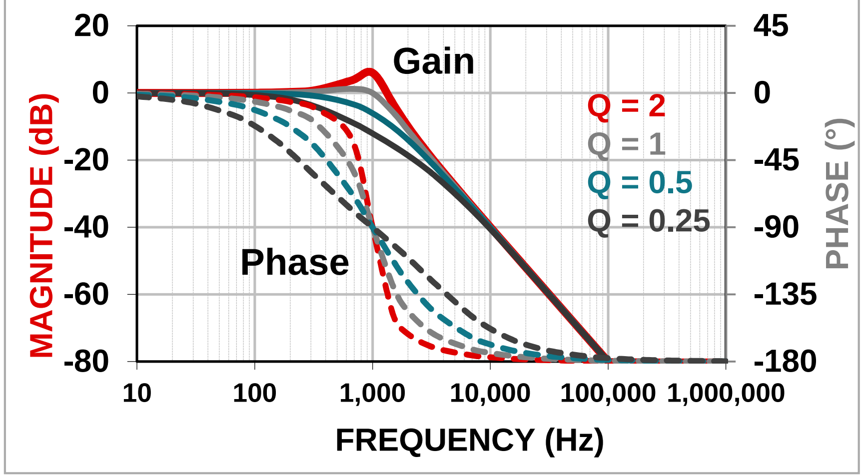
Inverted zero	Right-half-plane zero
$H(s)=\dfrac{1+\dfrac{\omega_Z}{s}}{1}$	$H(s)=\dfrac{1-\dfrac{s}{\omega_Z}}{1}$

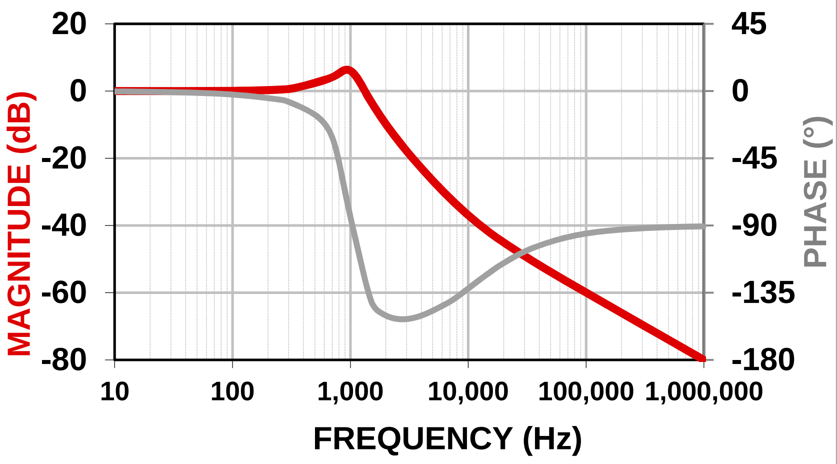




Complex conjugate pole and ESR zero

Complex conjugate pole	With ESR zero
$H(s)=\dfrac{1}{1+\dfrac{s}{Q_O\cdot\omega_O}+\dfrac{s^2}{\omega_O^2}}$	$H(s)=\dfrac{1+\dfrac{s}{\omega_Z}}{1+\dfrac{s}{Q_O\cdot\omega_O}+\dfrac{s^2}{\omega_O^2}}$



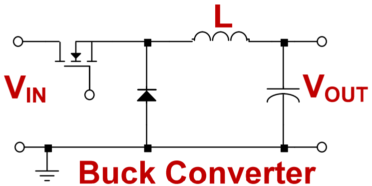


Control methods and operating modes

Control methods	• Voltage-mode control • Current-mode control
Operating modes	• Fixed frequency • Continuous conduction-mode (CCM)
Switching frequency and period	• Switching frequency – f_{SW} • Switching period – T $T = \frac{1}{f_{SW}}$

Buck, boost and buck-boost derived topologies

Buck, forward, push-pull, bridge



Buck Converter

$$V_{OUT} = V_{IN} \cdot D$$

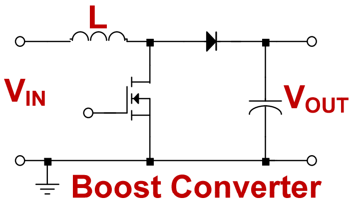
- Forward
- Two switch forward
- Active clamp forward
- Half bridge

$$V_{OUT} = V_{IN} \cdot D \cdot \frac{N_S}{N_P}$$

- Push-pull
- Full bridge
- Phase-shifted full bridge

$$V_{OUT} = V_{IN} \cdot 2 \cdot D \cdot \frac{N_S}{N_P}$$

Boost



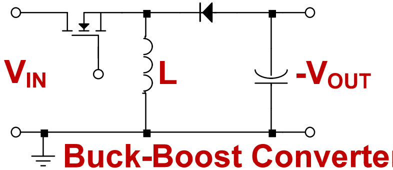
Boost Converter

$$V_{OUT} = V_{IN} \cdot \frac{1}{D'}$$

- Boost topology

On-time duty cycle: D
Off-time duty cycle: D′ = 1 - D

Buck-boost, SEPIC, flyback



Buck-Boost Converter

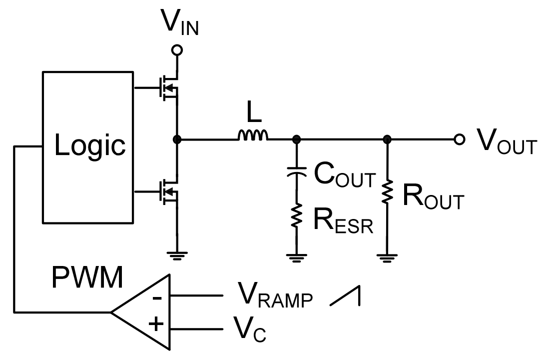
$$V_{OUT} = V_{IN} \cdot \frac{D}{D'}$$

- Buck-boost derived topologies
- SEPIC
- Cuk

- Flyback

$$V_{OUT} = V_{IN} \cdot \frac{D}{D'} \cdot \frac{N_S}{N_P}$$

Voltage-mode buck power stage

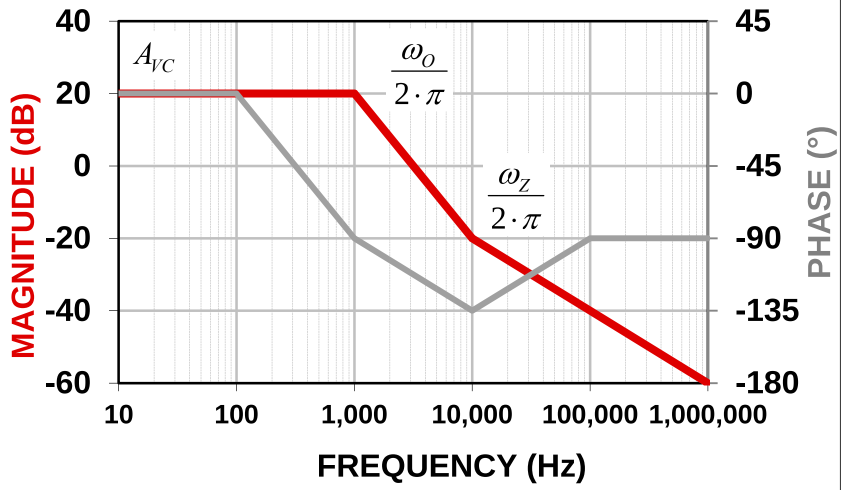


$$A_{VC} = \frac{V_{IN}}{V_{RAMP}}$$

$$\omega_O = \frac{1}{\sqrt{L \cdot C_{OUT}}}$$

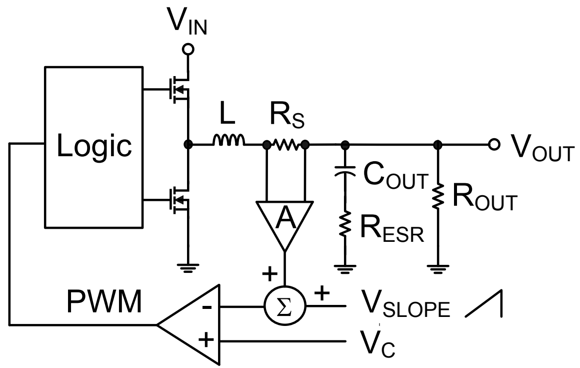
$$Q_O = \frac{R_{OUT}}{\sqrt{L / C_{OUT}}}$$

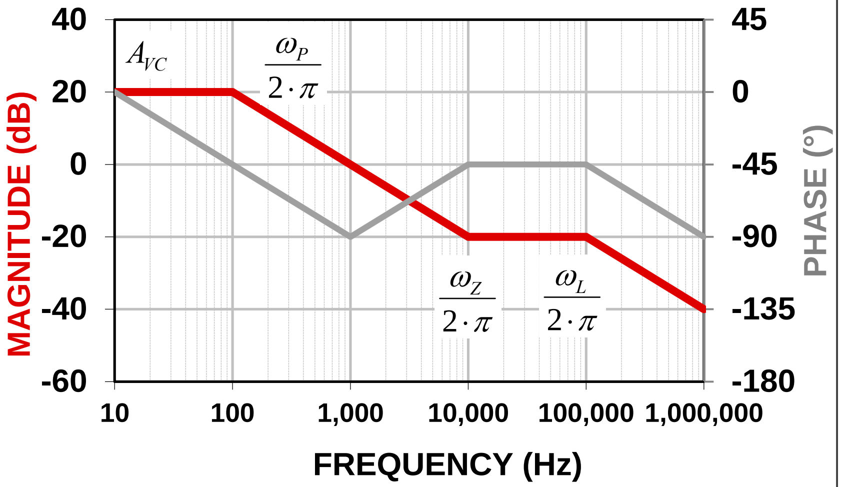
$$\omega_Z = \frac{1}{R_{ESR} \cdot C_{OUT}}$$



$$\frac{\hat{v}_{OUT}}{\hat{v}_C} = A_{VC} \cdot \frac{1 + \frac{s}{\omega_Z}}{1 + \frac{s}{Q_O \cdot \omega_O} + \frac{s^2}{\omega_O^{\,2}}}$$

Current-mode buck power stage





$$R_i = A \cdot R_S$$

$$\omega_Z = \frac{1}{R_{ESR} \cdot C_{OUT}}$$

$$A_{VC} \approx \frac{R_{OUT}}{R_i}$$

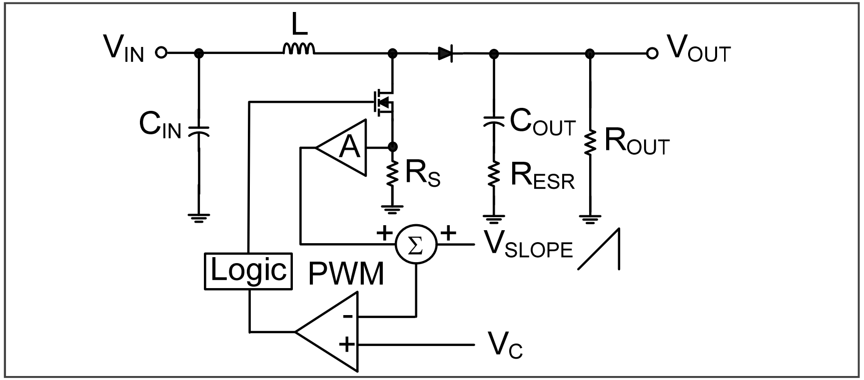
$$K_m \approx \frac{V_{IN}}{V_{SLOPE}}$$ at D = 0.5

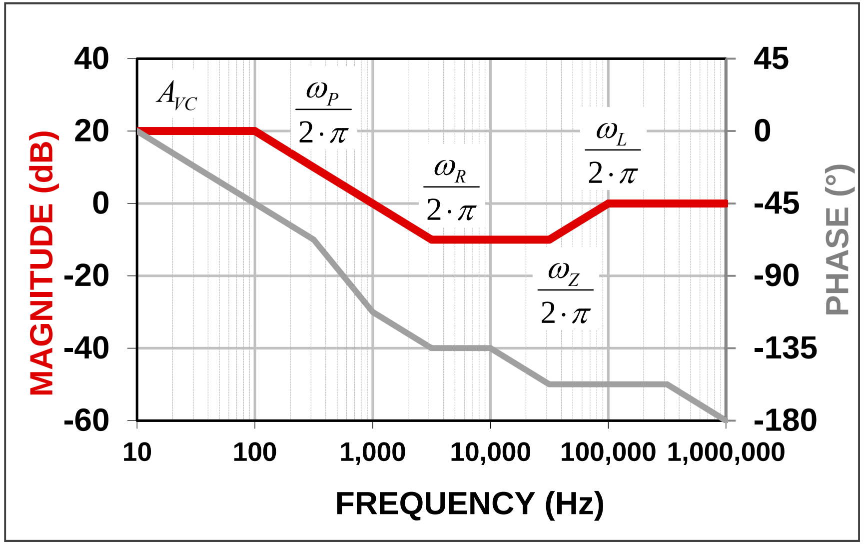
$$\omega_P \approx \frac{1}{C_{OUT} \cdot R_{OUT}}$$

$$\omega_L = \frac{K_m \cdot R_i}{L}$$

$$\frac{\hat{v}_{OUT}}{\hat{v}_C} \approx A_{VC} \cdot \frac{1 + \frac{s}{\omega_Z}}{\left(1 + \frac{s}{\omega_P}\right) \cdot \left(1 + \frac{s}{\omega_L}\right)}$$

Current-mode boost power stage





$$R_i = A \cdot R_S \qquad \omega_R = \frac{R_{OUT} \cdot D'^2}{L} \qquad \omega_L = \frac{K_m \cdot R_i}{L}$$

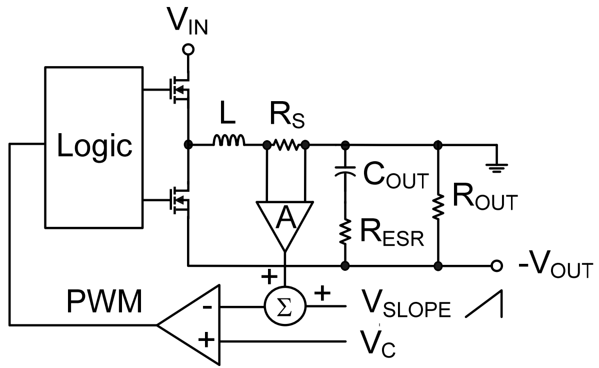
$$A_{VC} \approx \frac{R_{OUT} \cdot D'}{2 \cdot R_i} \qquad \omega_Z = \frac{1}{R_{ESR} \cdot C_{OUT}}$$

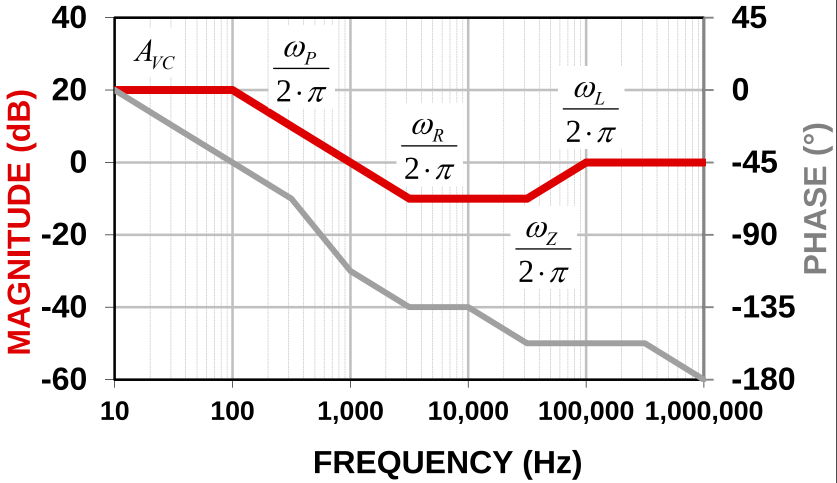
$$\omega_P \approx \frac{2}{C_{OUT} \cdot R_{OUT}} \qquad K_m \approx \frac{V_{OUT}}{V_{SLOPE}}$$

at D = 0.5

$$\frac{\hat{v}_{OUT}}{\hat{v}_C} \approx A_{VC} \cdot \frac{\left(1 - \frac{s}{\omega_R}\right) \cdot \left(1 + \frac{s}{\omega_Z}\right)}{\left(1 + \frac{s}{\omega_P}\right) \cdot \left(1 + \frac{s}{\omega_L}\right)}$$

Current-mode buck-boost power stage





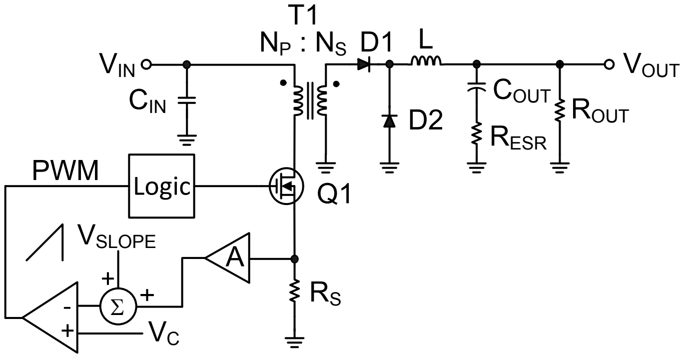
$$R_i = A \cdot R_S \qquad \omega_R = \frac{R_{OUT} \cdot D'^2}{L \cdot D} \qquad \omega_L = \frac{K_m \cdot R_i}{L}$$

$$A_{VC} \approx \frac{R_{OUT} \cdot D'}{(1+D) \cdot R_i} \qquad \omega_Z = \frac{1}{R_{ESR} \cdot C_{OUT}}$$

$$\omega_P \approx \frac{1+D}{C_{OUT} \cdot R_{OUT}} \qquad K_m \approx \frac{V_{IN} + V_{OUT}}{V_{SLOPE}}$$ at D = 0.5

$$\frac{\hat{v}_{OUT}}{\hat{v}_C} \approx A_{VC} \cdot \frac{\left(1 - \frac{s}{\omega_R}\right) \cdot \left(1 + \frac{s}{\omega_Z}\right)}{\left(1 + \frac{s}{\omega_P}\right) \cdot \left(1 + \frac{s}{\omega_L}\right)}$$

Current-mode forward power stage



$$R_i = A \cdot R_S$$

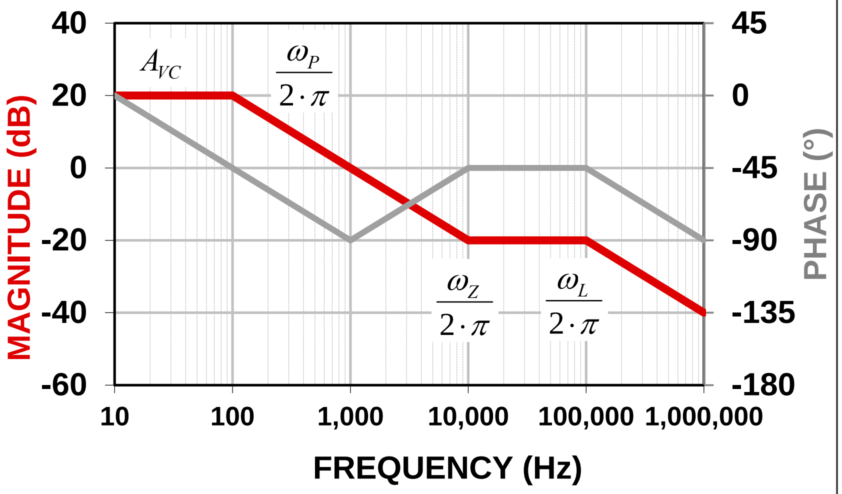
$$A_{VC} \approx \frac{R_{OUT}}{R_i} \cdot \frac{N_P}{N_S}$$

$$\omega_P \approx \frac{1}{C_{OUT} \cdot R_{OUT}}$$

$$\omega_Z = \frac{1}{R_{ESR} \cdot C_{OUT}}$$

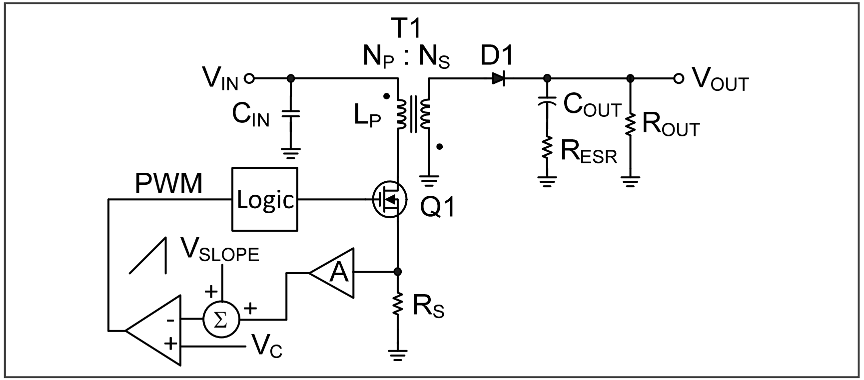
$$K_m \approx \frac{V_{IN}}{V_{SLOPE}}$$ at D = 0.5

$$\omega_L = \frac{K_m \cdot R_i}{L} \cdot \left(\frac{N_S}{N_P}\right)^2$$



$$\frac{\hat{v}_{OUT}}{\hat{v}_C} \approx A_{VC} \cdot \frac{1+\frac{s}{\omega_Z}}{\left(1+\frac{s}{\omega_P}\right)\cdot\left(1+\frac{s}{\omega_L}\right)}$$

Current-mode flyback power stage



$$R_i = A \cdot R_S$$

$$A_{VC} \approx \frac{R_{OUT} \cdot D'}{(1+D) \cdot R_i} \cdot \frac{N_P}{N_S}$$

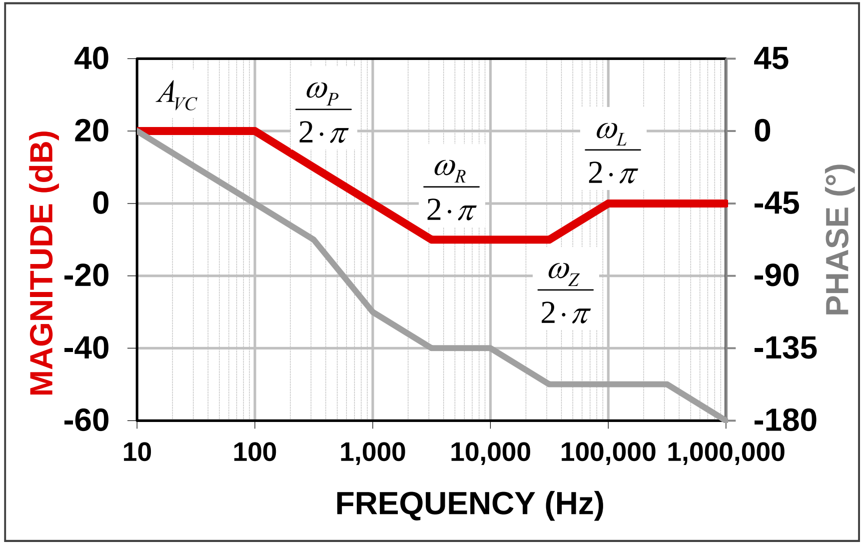
$$\omega_R = \frac{R_{OUT} \cdot D'^2}{L_P \cdot D} \cdot \left(\frac{N_P}{N_S}\right)^2$$

$$\omega_P \approx \frac{1+D}{C_{OUT} \cdot R_{OUT}}$$

$$K_m \approx \frac{V_{IN} + V_{OUT} \cdot \frac{N_P}{N_S}}{V_{SLOPE}}$$ at D = 0.5

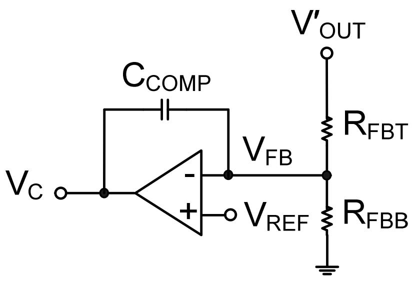
$$\omega_Z = \frac{1}{R_{ESR} \cdot C_{OUT}}$$

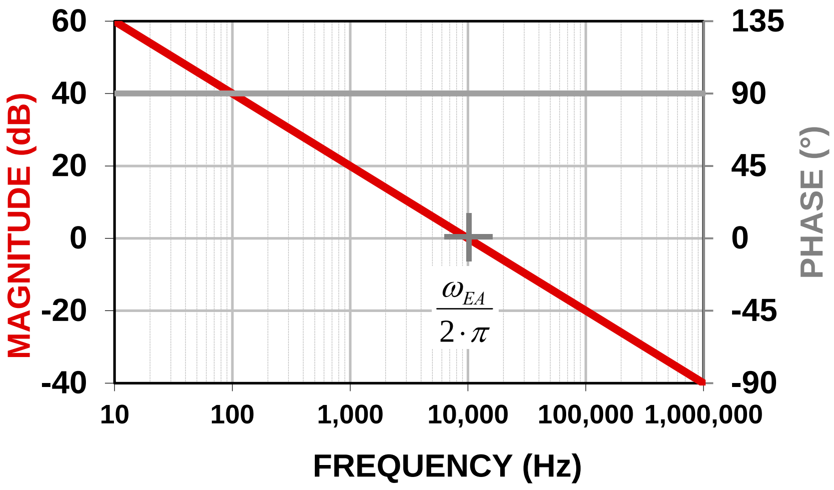
$$\omega_L = \frac{K_m \cdot R_i}{L_P}$$



$$\frac{\hat{v}_{OUT}}{\hat{v}_C} \approx A_{VC} \cdot \frac{\left(1 - \frac{s}{\omega_R}\right) \cdot \left(1 + \frac{s}{\omega_Z}\right)}{\left(1 + \frac{s}{\omega_P}\right) \cdot \left(1 + \frac{s}{\omega_L}\right)}$$

Type I error amplifier

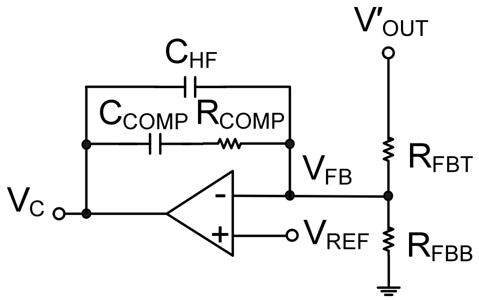


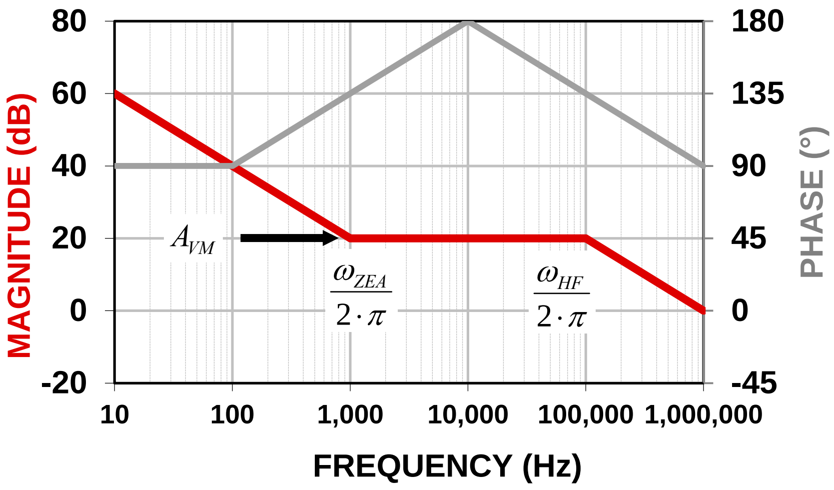


$$\omega_{EA} = \frac{1}{R_{FBT} \cdot C_{COMP}}$$

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -\frac{\omega_{EA}}{s}$$

Type II error amplifier





$$A_{VM} \approx \frac{R_{COMP}}{R_{FBT}}$$

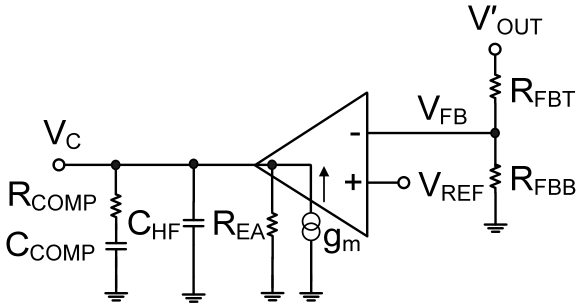
$$\omega_{ZEA} = \frac{1}{R_{COMP} \cdot C_{COMP}}$$

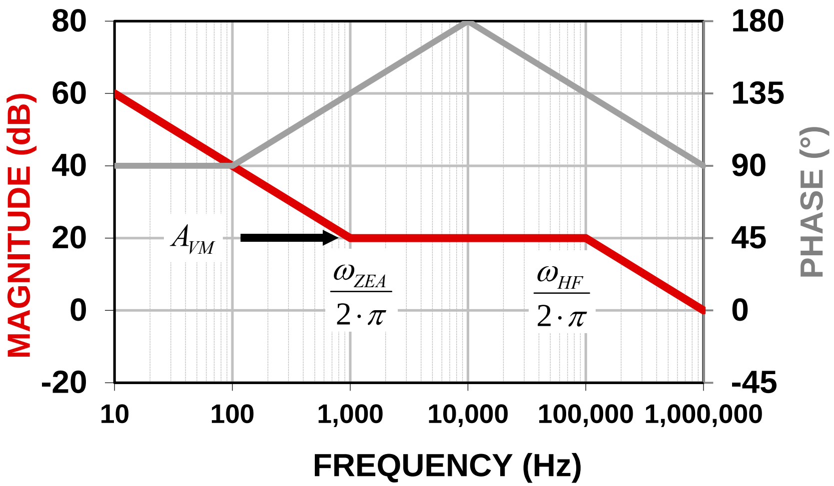
$$\omega_{HF} \approx \frac{1}{R_{COMP} \cdot C_{HF}}$$

Assumption: $C_{COMP} >> C_{HF}$

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -A_{VM} \cdot \frac{1+\frac{\omega_{ZEA}}{s}}{1+\frac{s}{\omega_{HF}}} \approx -\frac{A_{VM} \cdot \omega_{ZEA}}{s} \cdot \frac{1+\frac{s}{\omega_{ZEA}}}{1+\frac{s}{\omega_{HF}}}$$

Type II transconductance amplifier





$$A_{VM} = K_{FB}\cdot g_m \cdot R_{COMP}$$

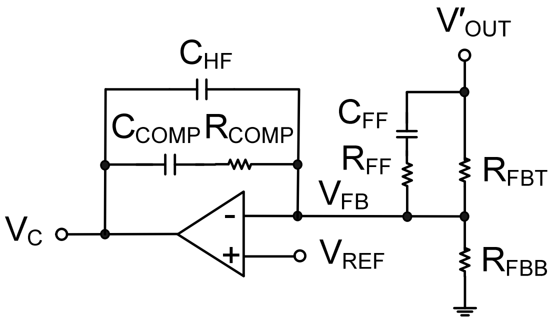
$$\omega_{ZEA} = \frac{1}{R_{COMP}\cdot C_{COMP}} \qquad K_{FB} = \frac{R_{FBB}}{R_{FBB}+R_{FBT}}$$

$$\omega_{HF} \approx \frac{1}{R_{COMP}\cdot C_{HF}} \qquad A_{OL} = g_m \cdot R_{EA}$$

Assumptions: $C_{COMP} >> C_{HF}$ & $R_{EA} >> R_{COMP}$

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -A_{VM}\cdot\frac{1+\frac{\omega_{ZEA}}{s}}{1+\frac{s}{\omega_{HF}}} \approx -\frac{A_{VM}\cdot\omega_{ZEA}}{s}\cdot\frac{1+\frac{s}{\omega_{ZEA}}}{1+\frac{s}{\omega_{HF}}}$$

Type III error amplifier

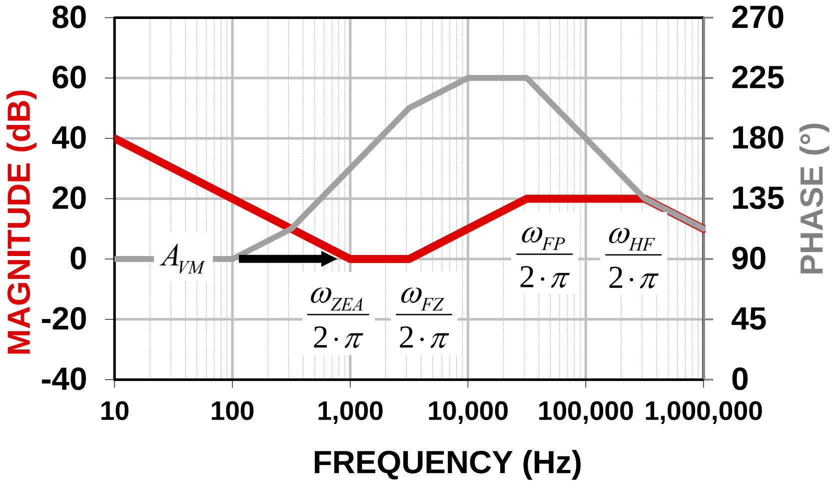


$$A_{VM} \approx \frac{R_{COMP}}{R_{FBT}}$$

$$\omega_{ZEA} = \frac{1}{R_{COMP} \cdot C_{COMP}} \qquad \omega_{FZ} \approx \frac{1}{R_{FBT} \cdot C_{FF}}$$

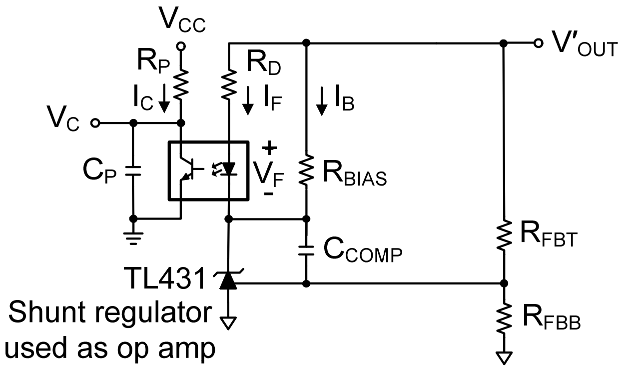
$$\omega_{FP} = \frac{1}{R_{FF} \cdot C_{FF}} \qquad \omega_{HF} \approx \frac{1}{R_{COMP} \cdot C_{HF}}$$

Assumptions: $C_{COMP} >> C_{HF}$ & $R_{FBT} >> R_{FF}$



$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} = -A_{VM} \cdot \frac{\left(1+\frac{\omega_{ZEA}}{s}\right)\cdot\left(1+\frac{s}{\omega_{FZ}}\right)}{\left(1+\frac{s}{\omega_{FP}}\right)\cdot\left(1+\frac{s}{\omega_{HF}}\right)} = -\frac{A_{VM}\cdot\omega_{ZEA}}{s} \cdot \frac{\left(1+\frac{s}{\omega_{ZEA}}\right)\cdot\left(1+\frac{s}{\omega_{FZ}}\right)}{\left(1+\frac{s}{\omega_{FP}}\right)\cdot\left(1+\frac{s}{\omega_{HF}}\right)}$$

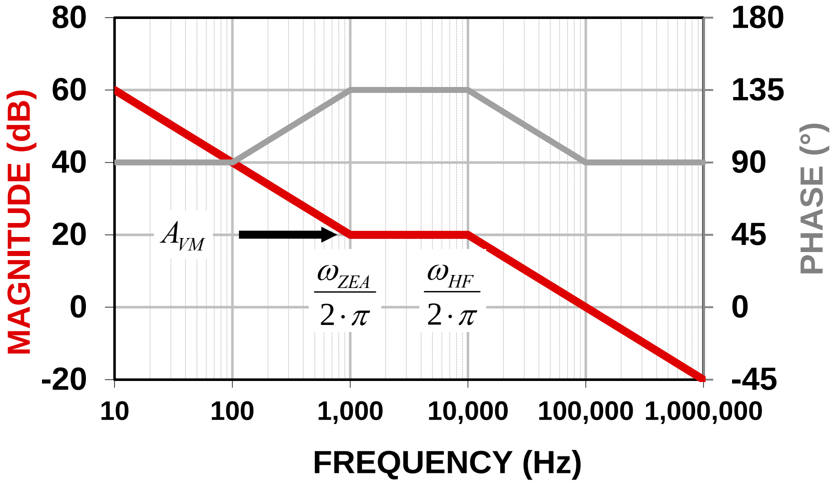
Isolated feedback with optocoupler



$$A_{VM} = CTR \cdot \frac{R_P}{R_D} \qquad CTR = \frac{I_C}{I_F}$$

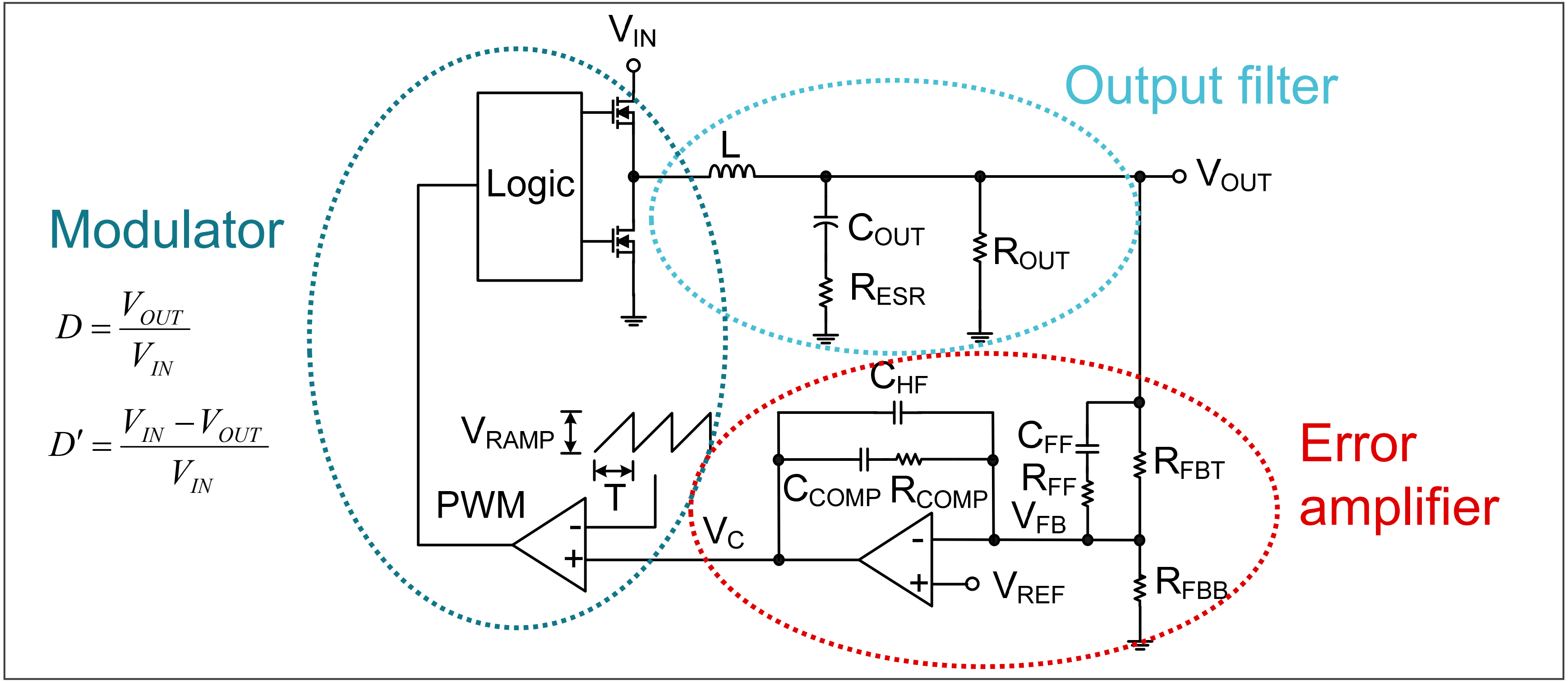
$$\omega_{ZEA} = \frac{1}{R_{FBT} \cdot C_{COMP}}$$

$$\omega_{HF} = \frac{1}{R_P \cdot C_P}$$



$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -A_{VM} \cdot \frac{1+\frac{\omega_{ZEA}}{s}}{1+\frac{s}{\omega_{HF}}} \approx -\frac{A_{VM}\cdot\omega_{ZEA}}{s} \cdot \frac{1+\frac{s}{\omega_{ZEA}}}{1+\frac{s}{\omega_{HF}}}$$

Voltage-mode buck



Voltage-mode buck compensation strategy

- Choose a value for R_{FBT} based on bias current and power dissipation
- Pick target bandwidth, typically $f_{SW}/10$:

  $\omega_C = 2\cdot\pi\cdot f_C$
- Find the mid-band gain A_{VM} to achieve target bandwidth
- Set ω_{ZEA} and ω_{FZ} equal to the output filter complex conjugate pole ω_O:

  $\omega_{ZEA} = \omega_{FZ} = \omega_O$
- Set ω_{FP} equal to the output filter zero ω_Z:

  $\omega_{FP} = \omega_Z$
- Set ω_{HF} equal to half the switching frequency:

  $\omega_{HF} = 2\cdot\pi\cdot f_{SW}/2$

$$A_{VM} = \frac{\omega_C}{A_{VC} \cdot \omega_O}$$

$$R_{COMP} = A_{VM} \cdot R_{FBT}$$

$$C_{COMP} = \frac{1}{\omega_{ZEA} \cdot R_{COMP}}$$

$$C_{FF} = \frac{1}{\omega_{FZ} \cdot R_{FBT}}$$

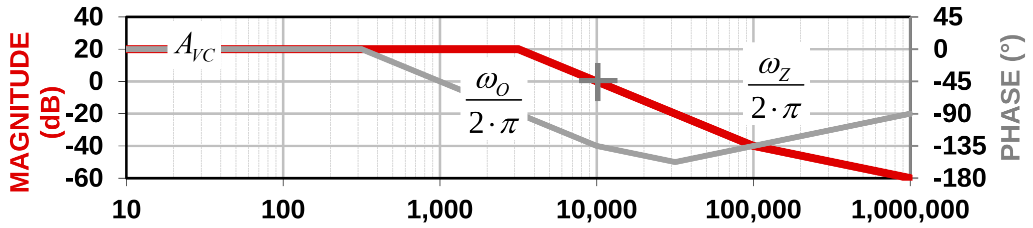
$$R_{FF} = \frac{1}{\omega_{FP} \cdot C_{FF}}$$

$$C_{HF} = \frac{1}{\omega_{HF} \cdot R_{COMP}}$$

Voltage-mode buck compensation results

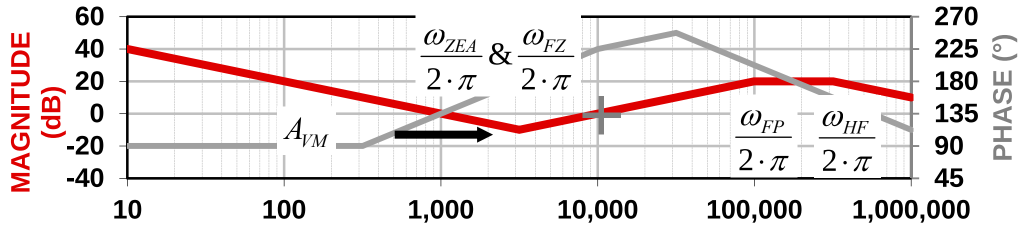
Power stage

$$\frac{\hat{v}_{OUT}}{\hat{v}_C} \approx A_{VC} \cdot \frac{1+\frac{s}{\omega_Z}}{1+\frac{s}{Q_O \cdot \omega_O}+\frac{s^2}{\omega_O^2}}$$



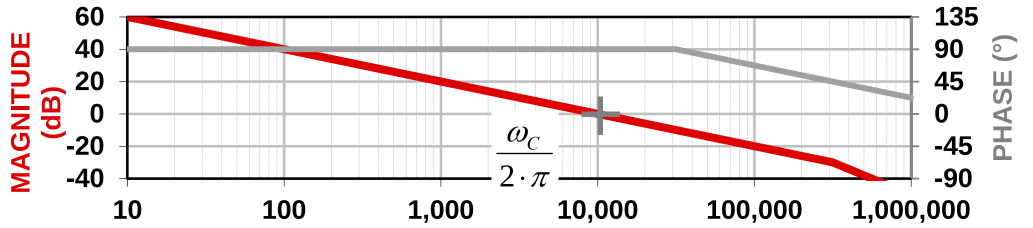
Error amplifier

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -A_{VM} \cdot \frac{\left(1+\frac{\omega_{ZEA}}{s}\right)\cdot\left(1+\frac{s}{\omega_{FZ}}\right)}{\left(1+\frac{s}{\omega_{FP}}\right)\cdot\left(1+\frac{s}{\omega_{HF}}\right)}$$



Control loop

$$\frac{\hat{v}_{OUT}}{\hat{v}'_{OUT}} = \frac{\hat{v}_{OUT}}{\hat{v}_C} \cdot \frac{\hat{v}_C}{\hat{v}'_{OUT}}$$

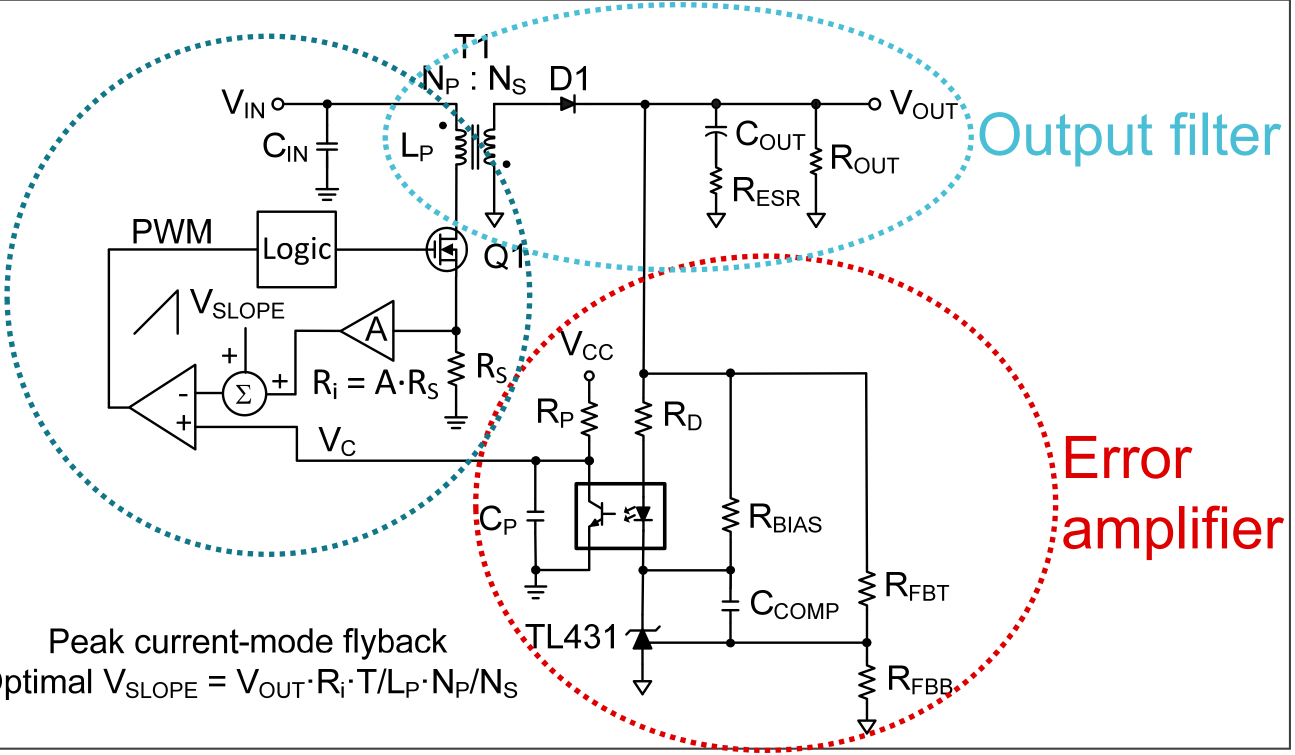


Isolated current-mode flyback

Modulator

$$D = \frac{V_{OUT}}{V_{IN} \cdot \frac{N_S}{N_P} + V_{OUT}}$$

$$D' = \frac{V_{IN}}{V_{IN} + V_{OUT} \cdot \frac{N_P}{N_S}}$$



Current-mode flyback compensation strategy

- Choose a value for R_{FBT} based on bias current and power dissipation
- Find the modulator transconductance in A/V
- Find the RHPZ frequency at minimum input voltage and maximum load current
- Set the target bandwidth to 1/4 of the RHPZ frequency:
  $\omega_C = 2 \cdot \pi \cdot f_C = \omega_R / 4$
- Find the mid-band gain A_{VM} to achieve target bandwidth
  Adjust R_D, R_P and C_{OUT} as required
- Set ω_{ZEA} equal to 1/10 the target crossover frequency:
  $\omega_{ZEA} = \omega_C / 10$
- Set ω_{HF} equal to the lower of the RHP or ESR zero frequency:
  $\omega_{HF} = \omega_R$ or ω_Z

$$G_m(\text{mod}) = \frac{D'}{R_i} \cdot \frac{N_P}{N_S}$$

$$\omega_R = \frac{R_{OUT} \cdot D'^2}{L_P \cdot D} \cdot \left(\frac{N_P}{N_S} \right)^2$$

$$A_{VM} = \frac{\omega_C \cdot C_{OUT}}{G_m(\text{mod})}$$

$$R_D = CTR \cdot \frac{R_P}{\text{A}_{\text{VM}}}$$

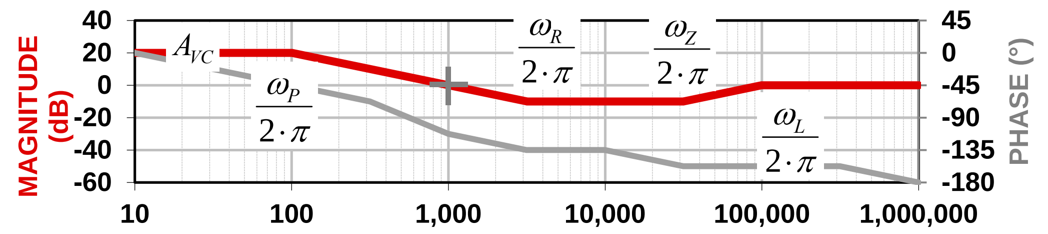
$$C_{COMP} = \frac{1}{R_{FBT} \cdot \omega_{ZEA}}$$

$$C_P = \frac{1}{R_P \cdot \omega_{HF}}$$

Current-mode flyback compensation results

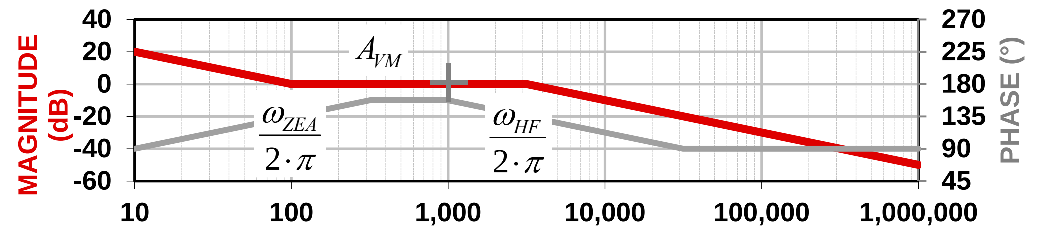
Power stage

$$\frac{\hat{v}_{OUT}}{\hat{v}_C} \approx A_{VC} \cdot \frac{\left(1-\frac{s}{\omega_R}\right)\cdot\left(1+\frac{s}{\omega_Z}\right)}{\left(1+\frac{s}{\omega_P}\right)\cdot\left(1+\frac{s}{\omega_L}\right)}$$



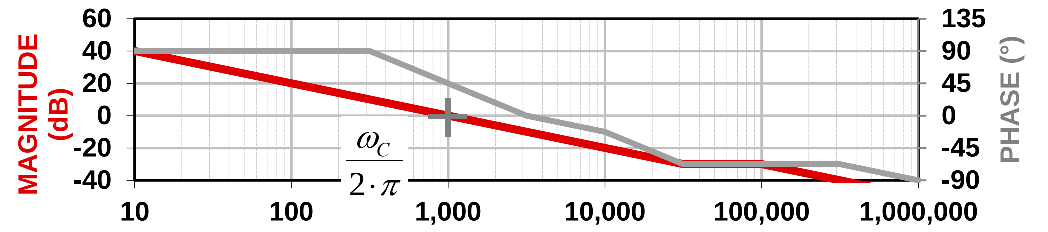
Error amplifier

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -A_{VM} \cdot \frac{1+\frac{\omega_{ZEA}}{s}}{1+\frac{s}{\omega_{HF}}}$$



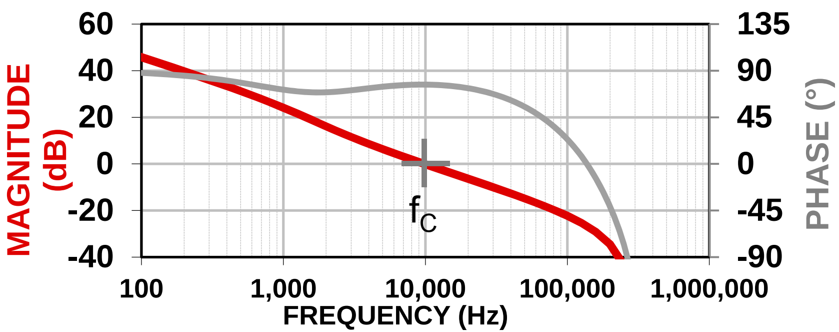
Control loop

$$\frac{\hat{v}_{OUT}}{\hat{v}'_{OUT}} = \frac{\hat{v}_{OUT}}{\hat{v}_C} \cdot \frac{\hat{v}_C}{\hat{v}'_{OUT}}$$

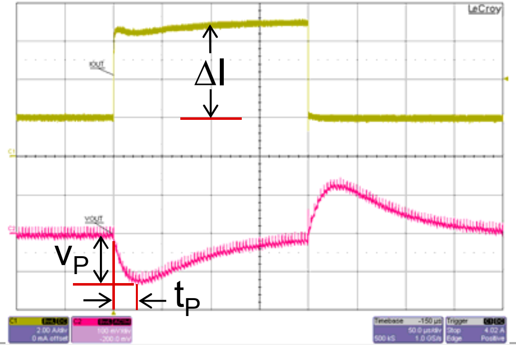


Bandwidth vs. transient response

Current-mode bandwidth



Current-mode transient response



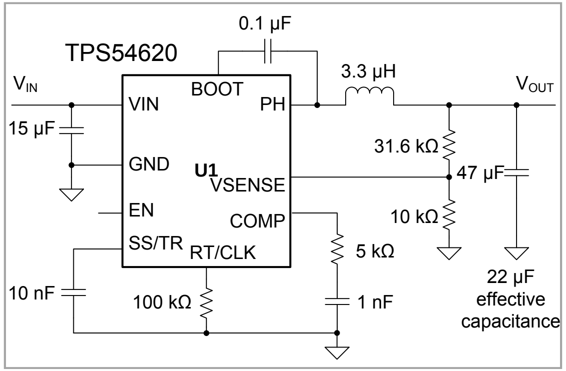
With no ESR, slew rate or duty cycle limiting: $t_P = \frac{1}{4 \cdot f_C}$ $\quad t_P = \frac{1}{4 \cdot 10kHz} = 25\mu s$

Current-mode single pole approximation: $V_P = \frac{\Delta I}{2 \cdot \pi \cdot f_C \cdot C_{OUT}}$ $\quad V_P = \frac{5A}{2 \cdot \pi \cdot 10kHz \cdot 440\mu F} = 180mV$

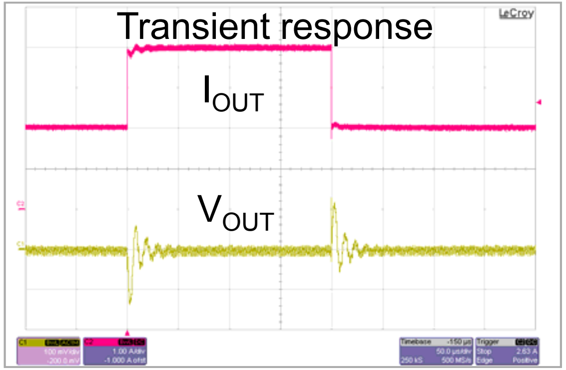
Current-mode critically damped: $V_P = \frac{\Delta I}{e \cdot \pi \cdot f_C \cdot C_{OUT}}$ $\quad V_P = \frac{5A}{e \cdot \pi \cdot 10kHz \cdot 440\mu F} = 130mV$ shown above

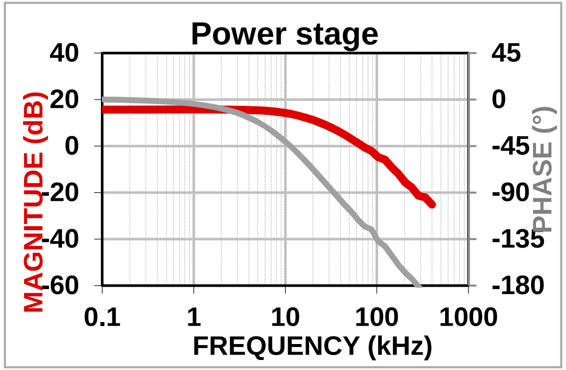
Voltage-mode: $V_P = \frac{\Delta I}{8 \cdot f_C \cdot C_{OUT}}$ $\quad V_P = \frac{5A}{8 \cdot 10kHz \cdot 440\mu F} = 140mV$

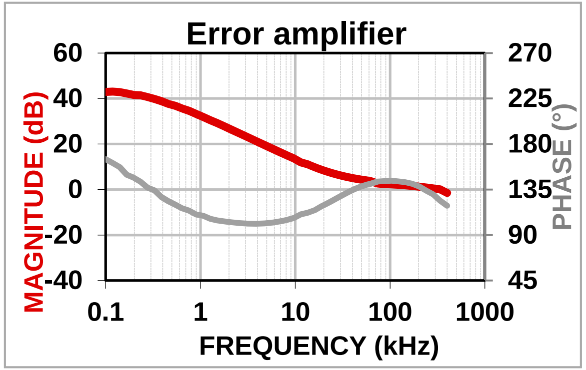
Switching regulator with poor compensation

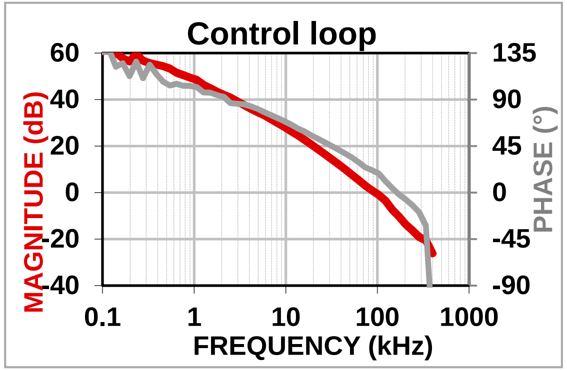


- Power stage: phase at –180° indicates high internal slope compensation
- Error amplifier: zero appears high and mid-band gain is 3 dB
- Control loop: f_C is 95 kHz with only 20° phase margin

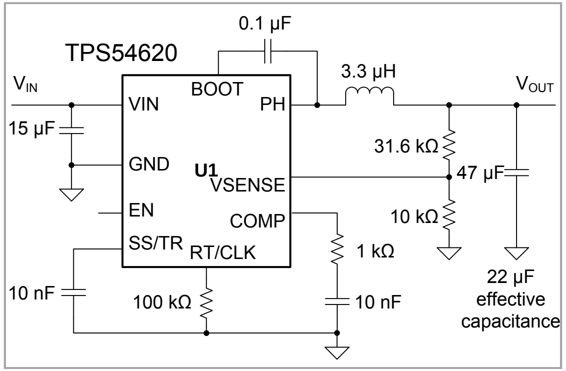




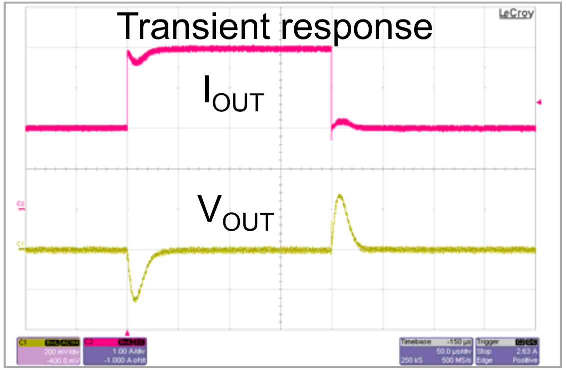


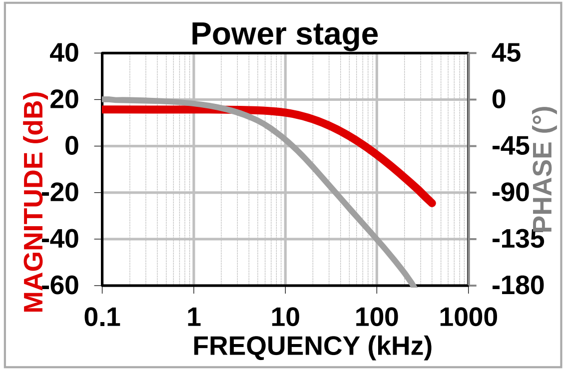


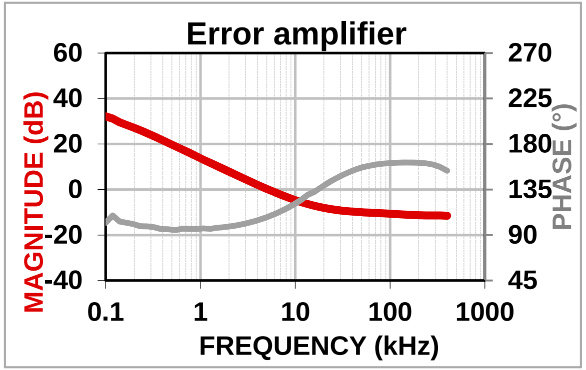
Switching regulator with revised compensation

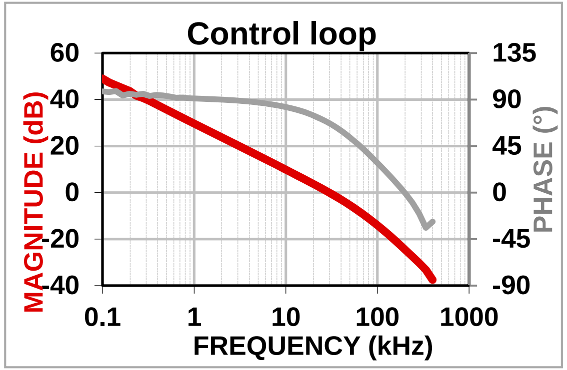


- Power stage: cannot change slope compensation
- Error amplifier: decrease R_{COMP} and rescale C_{COMP}
- Control loop: now f_C is 30 kHz with 67° phase margin



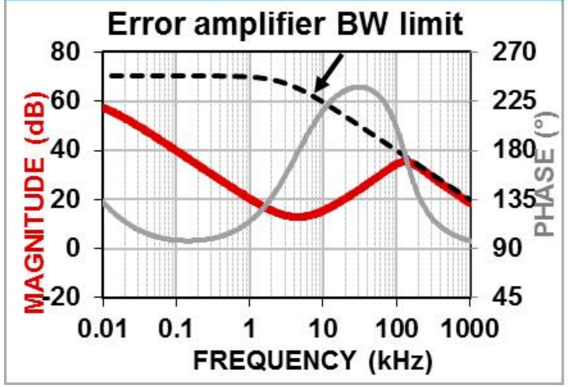






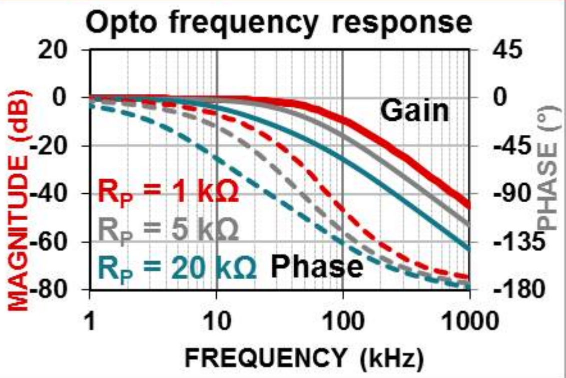
Practical limitations

Error amplifier bandwidth



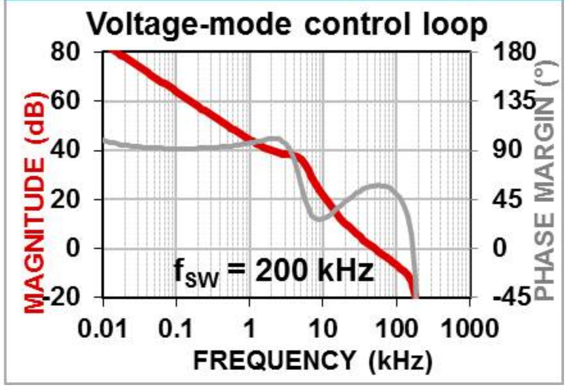
- Error amp BW can limit maximum f_C
- Wider BW op amp needed for voltage-mode due to Type III compensation

Optocoupler bandwidth



- Resistance seen by output transistor forms a pole in kHz range
- More of an issue for forward topologies at higher f_C

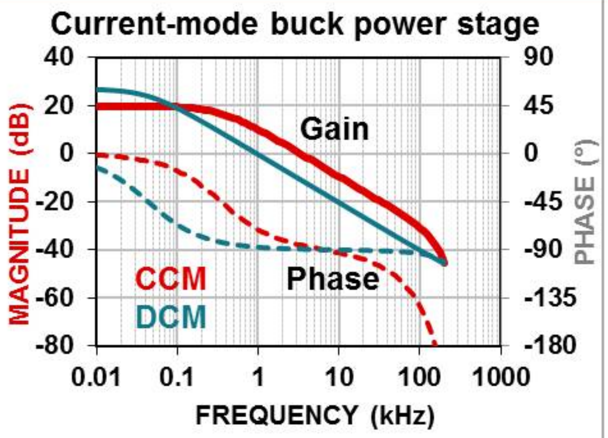
Switching frequency

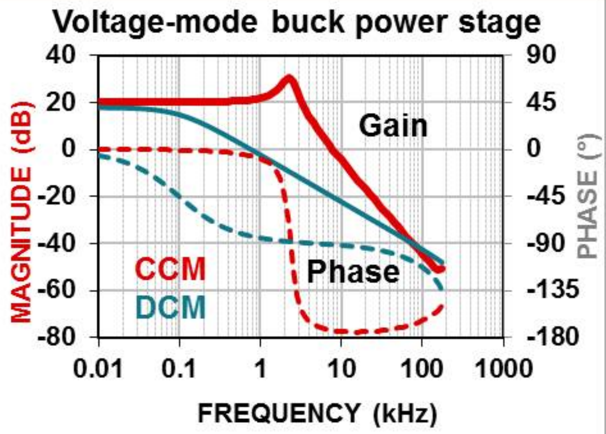


- Maximum f_C is a fraction of f_{SW}
- Rule of thumb is 1/5 to 1/10 of f_{SW}

DCM vs. CCM characteristics

Discontinuous vs. continuous conduction-mode





- Discontinuous conduction-mode (DCM) occurs when the inductor current dwells at zero before the end of the switching cycle
- This causes a reduction in the bandwidth
- Generally, if the loop is stable in CCM, it will be stable in DCM

DCM duty cycle

- Buck

$$D = \sqrt{\frac{2 \cdot L \cdot f_{SW} \cdot I_{OUT} \cdot V_{OUT}}{V_{IN} \cdot (V_{IN} - V_{OUT})}}$$

- Boost

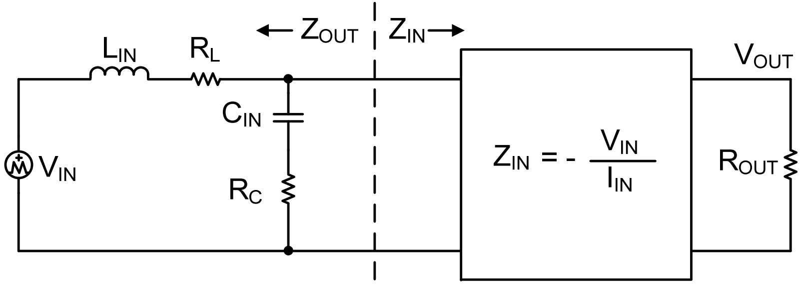
$$D = \frac{\sqrt{2 \cdot L \cdot f_{SW} \cdot I_{OUT} \cdot (V_{OUT} - V_{IN})}}{V_{IN}}$$

- Buck-boost

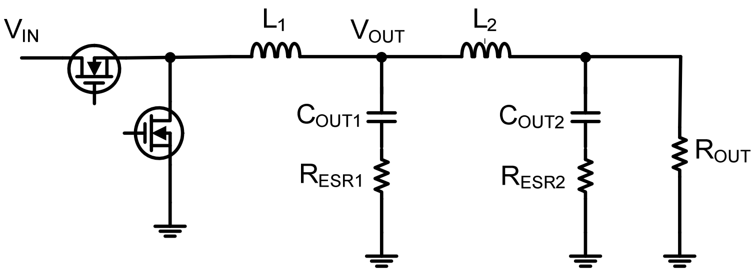
$$D = \frac{\sqrt{2 \cdot L \cdot f_{SW} \cdot I_{OUT} \cdot V_{OUT}}}{V_{IN}}$$

Filter considerations

Input filter stability



Second stage filters



For stability: Filter Z_{OUT} << Converter Z_{IN}

- Characteristic impedance $Z_S = \sqrt{\frac{L_{IN}}{C_{IN}}}$
- Damping factor

$$\zeta = \frac{1}{2} \cdot \left(\frac{R_L + R_C}{Z_S} + \frac{Z_S}{Z_{IN}} \right)$$

- Capacitors: make C_{OUT1} smaller than C_{OUT2}
- Inductors: make L_2 smaller than L_1
- Resonance: make second stage filter resonance 3 times f_C
- Damping: make second stage filter damped to a Q of 1

Summary

- Identify poles and zeros of the power stage
- Cancel with zeros and poles in the error amp
- Adjust the gain for best performance

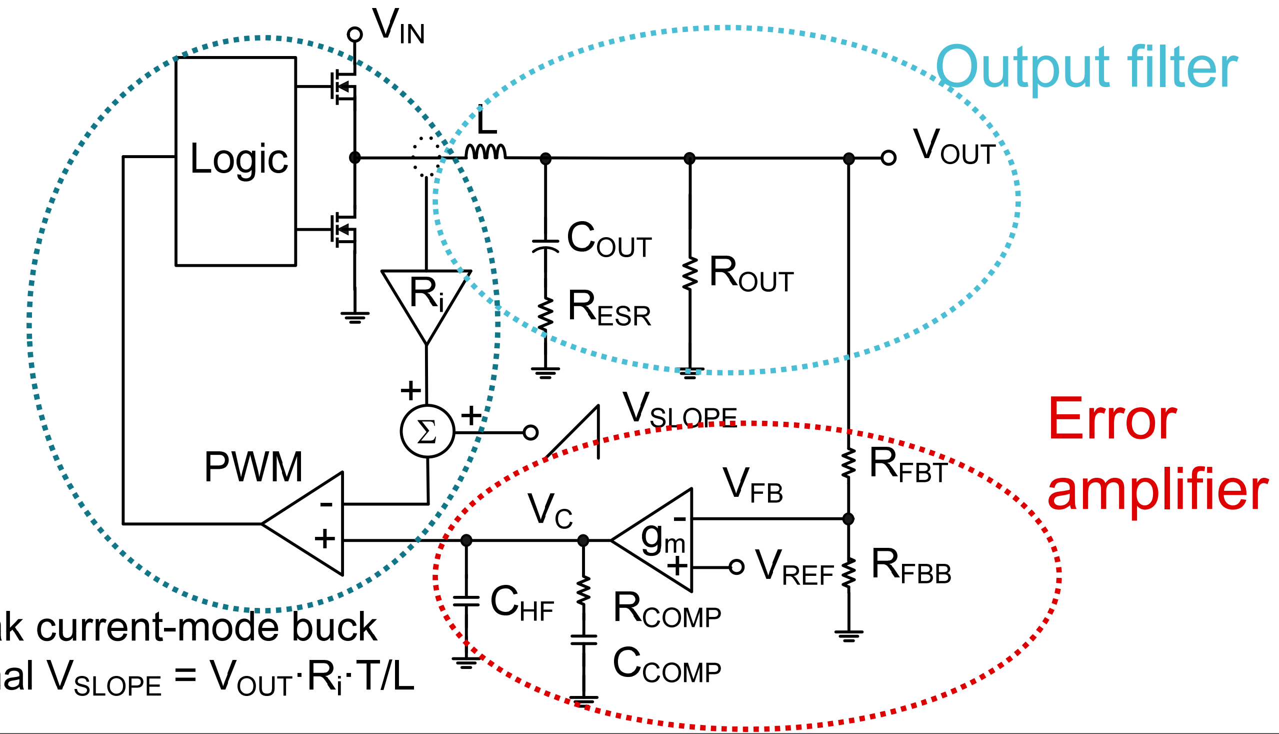
Resources and references

- "Closing the Feedback Loop" by Lloyd Dixon, SEM300
- "Current-Mode Control of Switching Power Supplies" by Lloyd Dixon, SEM400
- "The Right-Half-Plane Zero -- A Simplified Explanation" by Lloyd Dixon, SEM500
- "Isolating the Control Loop" by Robert Mammano, SEM700
- "Control Loop Design" by Lloyd Dixon, SEM800
- "Control Loop Cookbook" by Lloyd Dixon, SEM1100
- "A More Accurate Current-Mode Control Model" by Ray Ridley, SEM1300
- "Designing Stable Control Loops" by Dan Mitchell and Bob Mammano, SEM1400
- "Current-Mode Modeling – Reference Guide" by Robert Sheehan, SNVA542
- "Understanding and Applying Current-Mode Control Theory" by Robert Sheehan, SNVA555
- "Frequency Compensation and Power Stage Design for Buck Converters to Meet Load Transient Specifications" by S. Bag, R. Sheehan, et al., APEC 2014

Appendix

- Current-mode buck compensation
- Current-mode boost compensation
- Current-mode buck-boost compensation
- Isolated compensation techniques
- Isolated forward converter compensation

Current-mode buck



$$D = \frac{V_{OUT}}{V_{IN}}$$

$$D' = \frac{V_{IN} - V_{OUT}}{V_{IN}}$$

Peak current-mode buck

Optimal $V_{SLOPE} = V_{OUT} \cdot R_i \cdot T/L$

Current-mode buck compensation strategy

- Choose a value for R_{FBT} based on bias current and power dissipation
- Find the modulator transconductance in A/V
- Pick target bandwidth, typically $f_{SW}/10$:

  $\omega_C = 2 \cdot \pi \cdot f_C$
- Find the mid-band gain A_{VM} to achieve target bandwidth
- Set ω_{ZEA} equal to 1/10 the target crossover frequency:

  $\omega_{ZEA} = \omega_C/10$
- Set ω_{HF} equal to the ESR zero frequency:

  $\omega_{HF} = \omega_Z$

$$G_m(\text{mod}) = \frac{1}{R_i}$$

$$A_{VM} = \frac{\omega_C \cdot C_{OUT}}{G_m(\text{mod})}$$

$$R_{COMP} = A_{VM} \cdot R_{FBT} \text{ (op amp)}$$

$$R_{COMP} = \frac{A_{VM}}{g_m \cdot K_{FB}} \text{ (}g_m\text{ amp)}$$

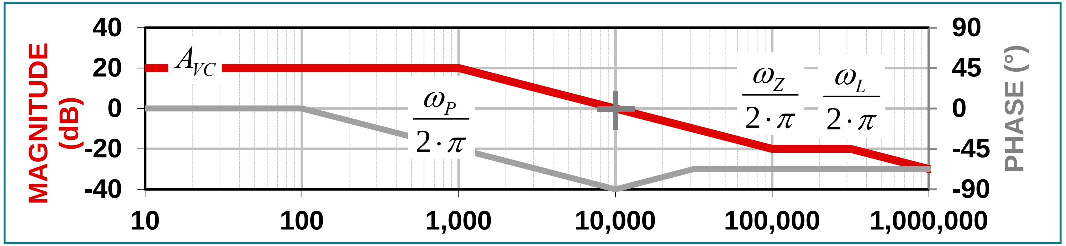
$$C_{COMP} = \frac{1}{\omega_{ZEA} \cdot R_{COMP}}$$

$$C_{HF} = \frac{1}{\omega_{HF} \cdot R_{COMP}}$$

Current-mode buck compensation results

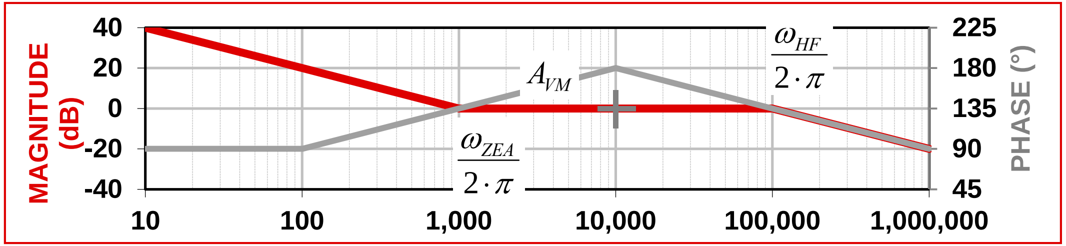
Power stage

$$\frac{\hat{v}_{OUT}}{\hat{v}_C} \approx A_{VC} \cdot \frac{1+\frac{s}{\omega_Z}}{\left(1+\frac{s}{\omega_P}\right)\cdot\left(1+\frac{s}{\omega_L}\right)}$$



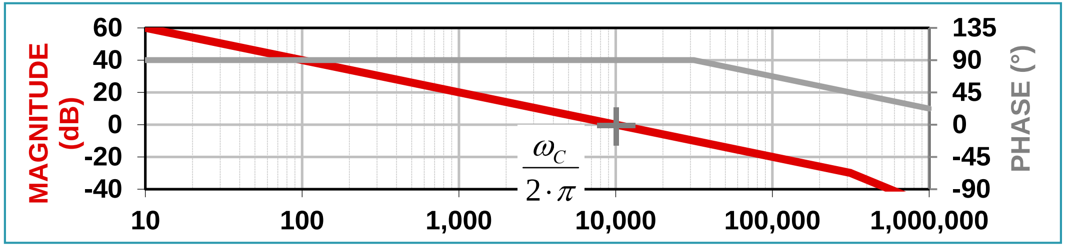
Error amplifier

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -A_{VM} \cdot \frac{1+\frac{\omega_{ZEA}}{s}}{1+\frac{s}{\omega_{HF}}}$$



Control loop

$$\frac{\hat{v}_{OUT}}{\hat{v}'_{OUT}} = \frac{\hat{v}_{OUT}}{\hat{v}_C} \cdot \frac{\hat{v}_C}{\hat{v}'_{OUT}}$$

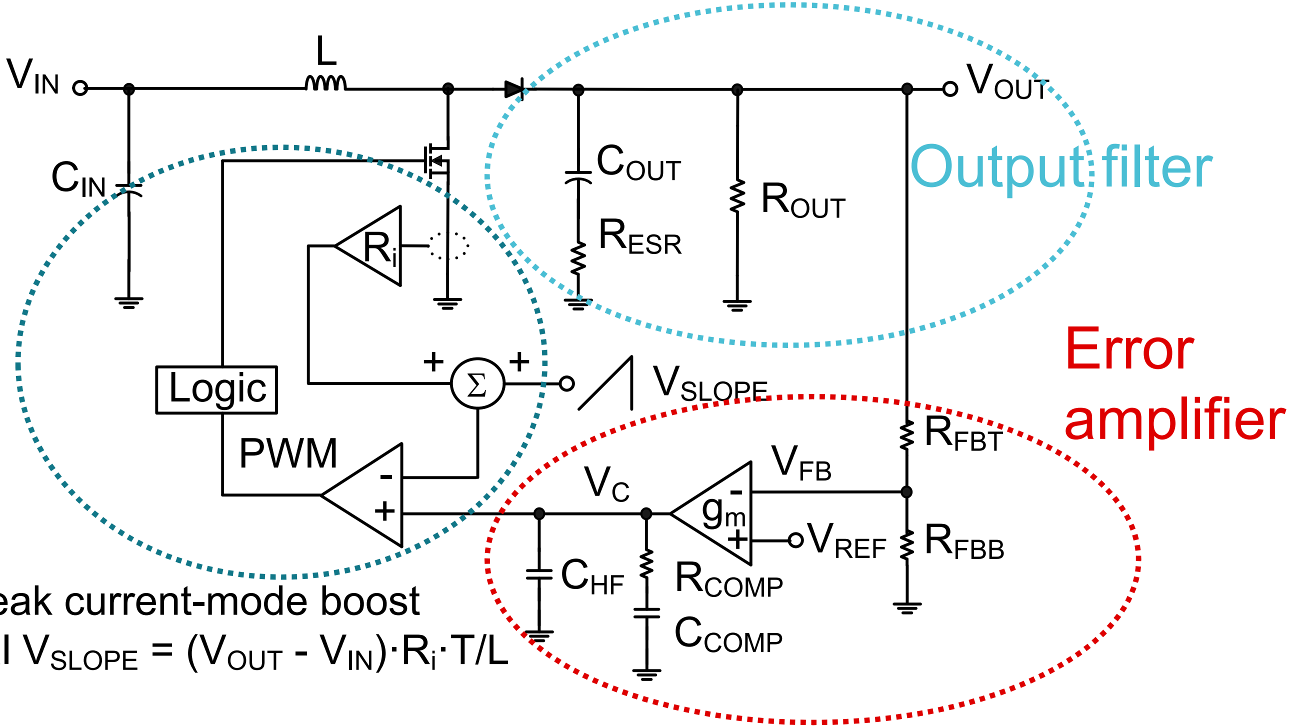


Current-mode boost

Modulator

$$D = \frac{V_{OUT} - V_{IN}}{V_{OUT}}$$

$$D' = \frac{V_{IN}}{V_{OUT}}$$



Peak current-mode boost

Optimal $V_{SLOPE} = (V_{OUT} - V_{IN}) \cdot R_i \cdot T/L$

Current-mode boost compensation strategy

- Choose a value for R_{FBT} based on bias current and power dissipation
- Find the modulator transconductance in A/V
- Find the RHPZ frequency at minimum input voltage and maximum load current
- Set the target bandwidth to 1/4 of the RHPZ frequency:

  $\omega_C = 2 \cdot \pi \cdot f_C = \omega_R / 4$
- Find the mid-band gain A_{VM} to achieve target bandwidth
- Set ω_{ZEA} equal to 1/10 the target crossover frequency:

  $\omega_{ZEA} = \omega_C / 10$
- Set ω_{HF} equal to the lower of the RHP or ESR zero frequency:

  $\omega_{HF} = \omega_R$ or ω_Z

$$G_m(\text{mod}) = \frac{D'}{R_i}$$

$$\omega_R = \frac{R_{OUT} \cdot D'^2}{L}$$

$$A_{VM} = \frac{\omega_C \cdot C_{OUT}}{G_m(\text{mod})}$$

$$R_{COMP} = A_{VM} \cdot R_{FBT} \text{ (op amp)}$$

$$R_{COMP} = \frac{A_{VM}}{g_m \cdot K_{FB}} \quad (g_m \text{ amp})$$

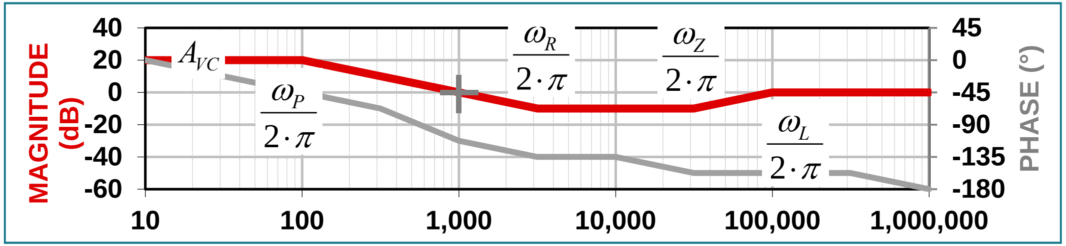
$$C_{COMP} = \frac{1}{\omega_{ZEA} \cdot R_{COMP}}$$

$$C_{HF} = \frac{1}{\omega_{HF} \cdot R_{COMP}}$$

Current-mode boost compensation results

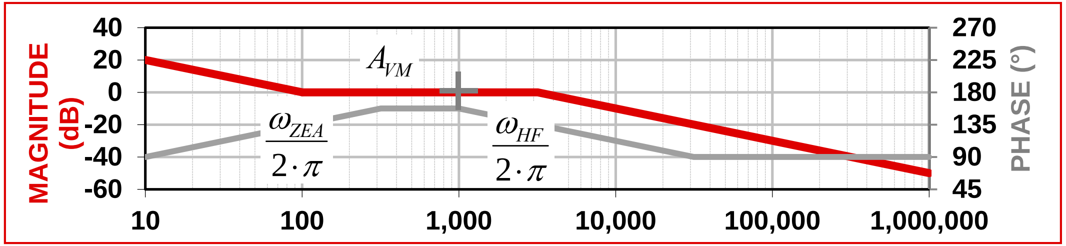
Power stage

$$\frac{\hat{v}_{OUT}}{\hat{v}_C} \approx A_{VC} \cdot \frac{\left(1-\frac{s}{\omega_R}\right)\cdot\left(1+\frac{s}{\omega_Z}\right)}{\left(1+\frac{s}{\omega_P}\right)\cdot\left(1+\frac{s}{\omega_L}\right)}$$



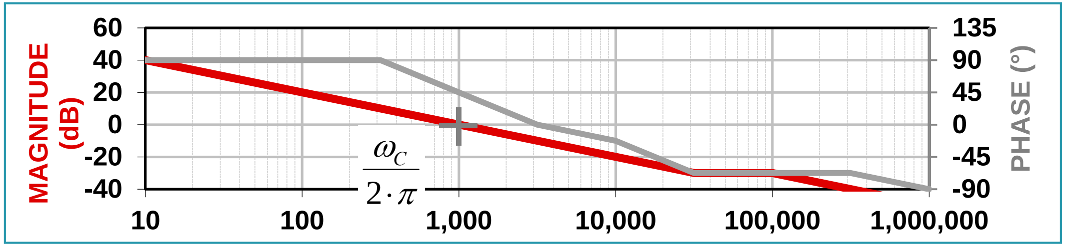
Error amplifier

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -A_{VM} \cdot \frac{1+\frac{\omega_{ZEA}}{s}}{1+\frac{s}{\omega_{HF}}}$$



Control loop

$$\frac{\hat{v}_{OUT}}{\hat{v}'_{OUT}} = \frac{\hat{v}_{OUT}}{\hat{v}_C} \cdot \frac{\hat{v}_C}{\hat{v}'_{OUT}}$$

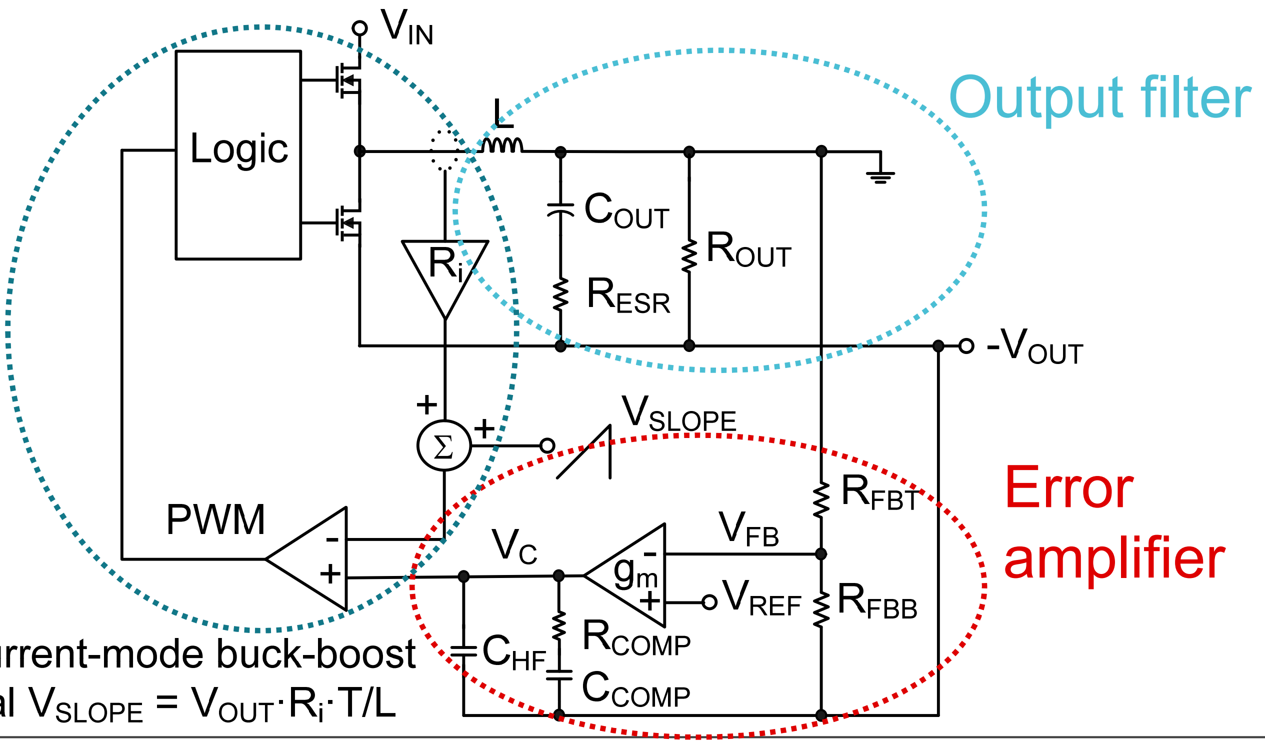


Current-mode buck-boost

Modulator

$$D = \frac{V_{OUT}}{V_{IN} + V_{OUT}}$$

$$D' = \frac{V_{IN}}{V_{IN} + V_{OUT}}$$



Peak current-mode buck-boost

Optimal $V_{SLOPE} = V_{OUT} \cdot R_i \cdot T/L$

Current-mode buck-boost compensation strategy

- Choose a value for R_{FBT} based on bias current and power dissipation
- Find the modulator transconductance in A/V
- Find the RHPZ frequency at minimum input voltage and maximum load current
- Set the target bandwidth to 1/4 of the RHPZ frequency:

  $\omega_C = 2\cdot\pi\cdot f_C = \omega_R/4$
- Find the mid-band gain A_{VM} to achieve target bandwidth
- Set ω_{ZEA} equal to 1/10 the target crossover frequency:

  $\omega_{ZEA} = \omega_C/10$
- Set ω_{HF} equal to the lower of the RHP or ESR zero frequency:

  $\omega_{HF} = \omega_R$ or ω_Z

$$G_m(\text{mod}) = \frac{D'}{R_i}$$

$$\omega_R = \frac{R_{OUT}\cdot D'^2}{L\cdot D}$$

$$A_{VM} = \frac{\omega_C\cdot C_{OUT}}{G_m(\text{mod})}$$

$$R_{COMP} = A_{VM}\cdot R_{FBT} \text{ (op amp)}$$

$$R_{COMP} = \frac{A_{VM}}{g_m\cdot K_{FB}} \quad (g_m \text{ amp})$$

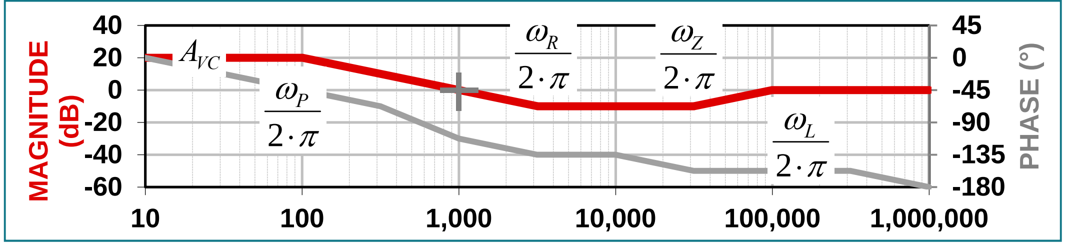
$$C_{COMP} = \frac{1}{\omega_{ZEA}\cdot R_{COMP}}$$

$$C_{HF} = \frac{1}{\omega_{HF}\cdot R_{COMP}}$$

Current-mode buck-boost compensation results

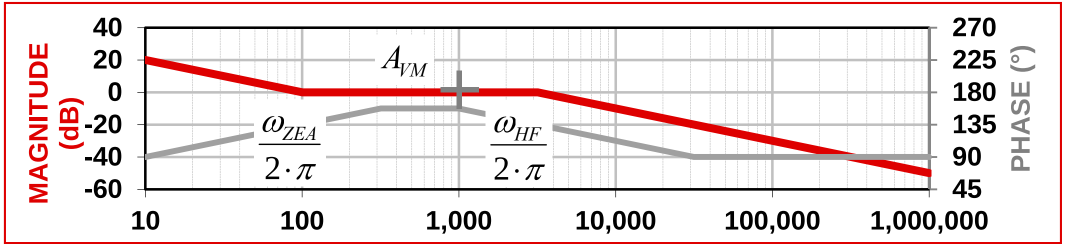
Power stage

$$\frac{\hat{v}_{OUT}}{\hat{v}_C} \approx A_{VC} \cdot \frac{\left(1-\frac{s}{\omega_R}\right)\cdot\left(1+\frac{s}{\omega_Z}\right)}{\left(1+\frac{s}{\omega_P}\right)\cdot\left(1+\frac{s}{\omega_L}\right)}$$



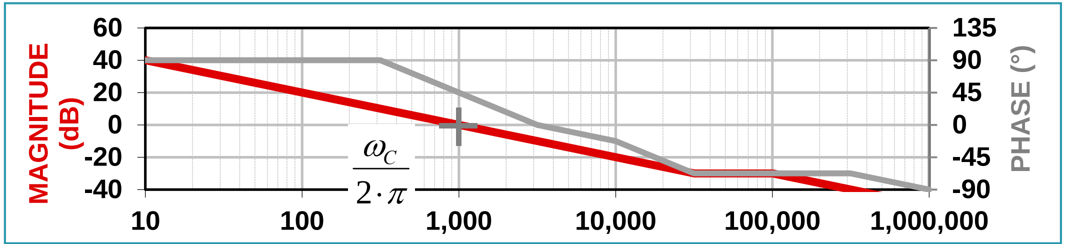
Error amplifier

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -A_{VM} \cdot \frac{1+\frac{\omega_{ZEA}}{s}}{1+\frac{s}{\omega_{HF}}}$$



Control loop

$$\frac{\hat{v}_{OUT}}{\hat{v}'_{OUT}} = \frac{\hat{v}_{OUT}}{\hat{v}_C} \cdot \frac{\hat{v}_C}{\hat{v}'_{OUT}}$$



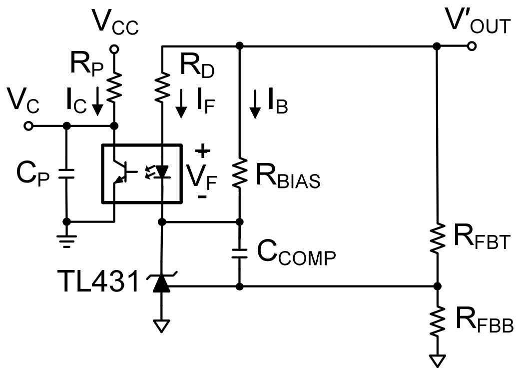
Isolated compensation techniques

Simplest method: Optocoupler with shunt regulator

- **CTR** – Current transfer ratio

$$CTR = \frac{I_C}{I_F}$$

- **C_P** – Includes opto parasitic capacitance. This creates a pole with gain setting resistor R_P



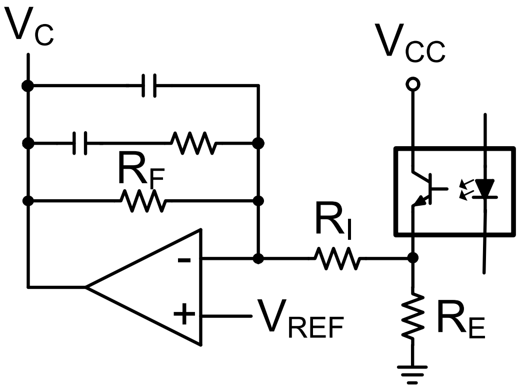
- **R_D** – Connected to V_{OUT} creates a feedback path even when C_{COMP} rolls off the gain

- **TL431** – Cathode cannot pull lower than the reference voltage

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -CTR \cdot \frac{R_P}{R_D} \cdot \frac{1+\dfrac{1}{s \cdot C_{COMP} \cdot R_{FBT}}}{1+s \cdot C_P \cdot R_P}$$

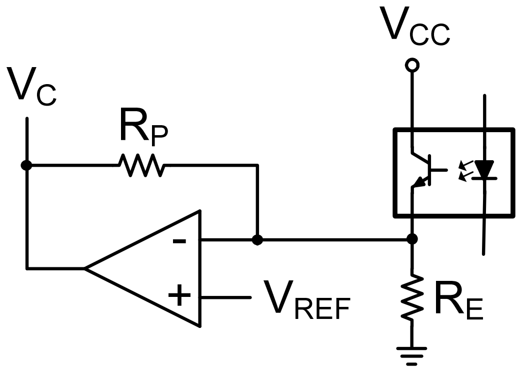
Primary side compensation

Primary side compensation



- Uses primary side inverting amplifier to implement frequency compensation

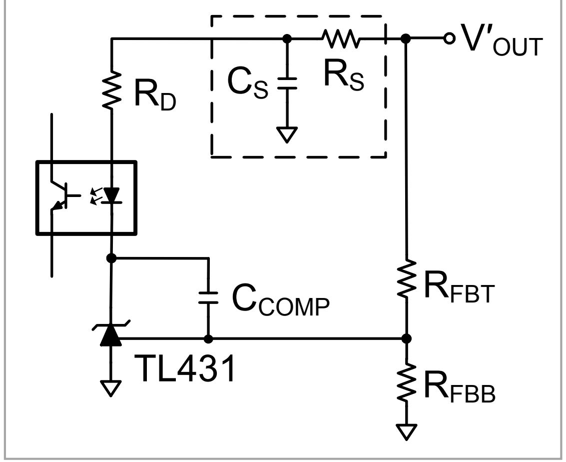
High bandwidth configuration



- Opto emitter is at virtual ground of V_{REF}
- This minimizes pole due to opto parasitic capacitance

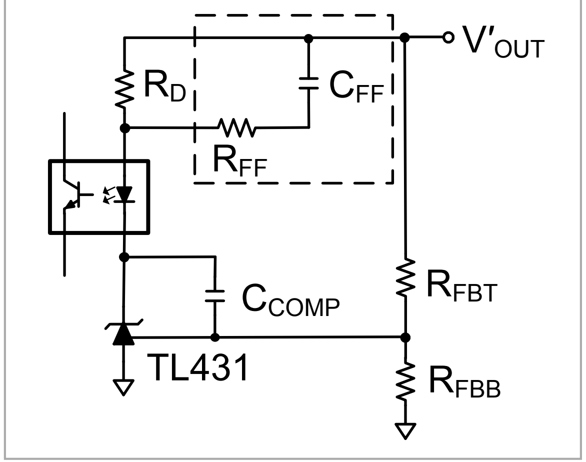
Secondary side compensation

ESR zero compensation



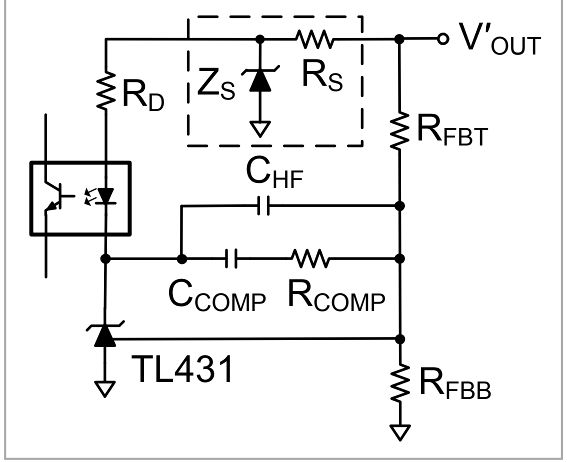
- An RC pole to the opto can be used to cancel the output capacitor ESR zero

Phase boost



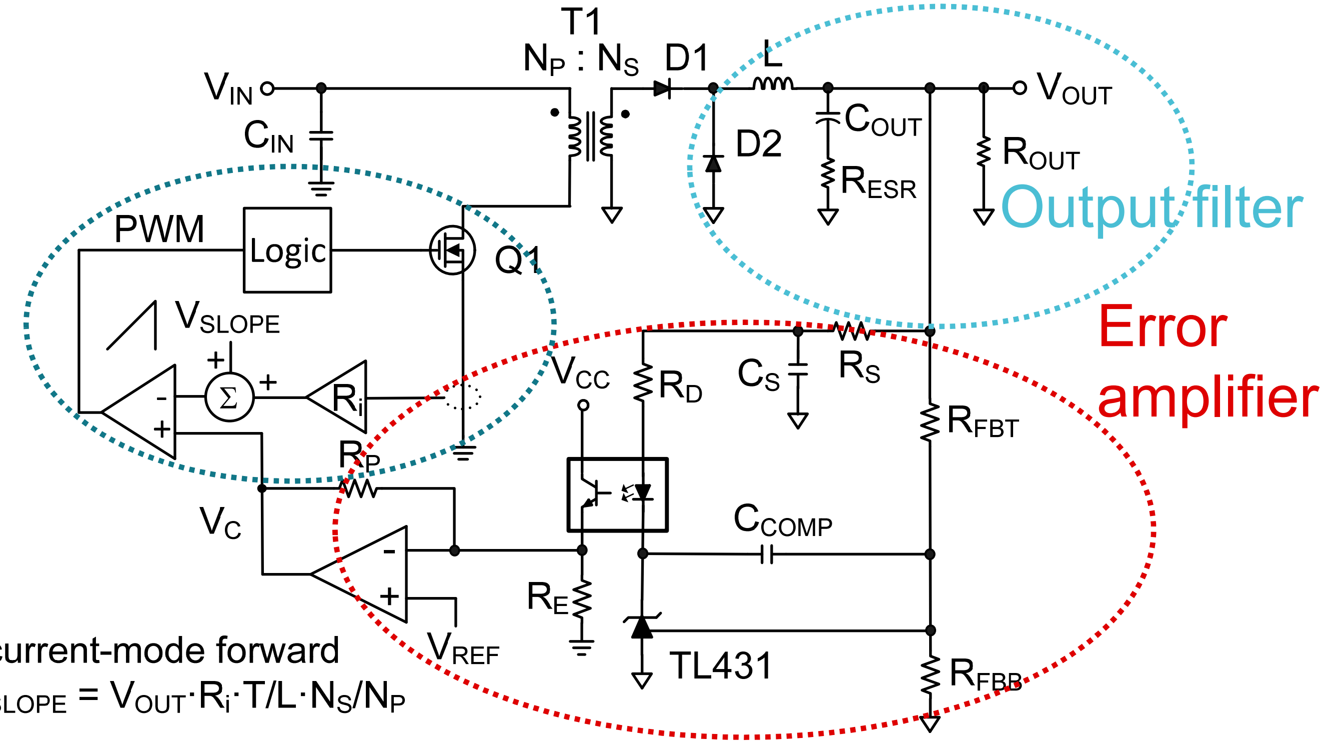
- Feed-forward across R_D adds phase boost for increased bandwidth

Zener bias



- Zener bias for R_D eliminates the high frequency feedback path for secondary-side compensation

Isolated current-mode forward



$$D = \frac{V_{OUT}}{V_{IN}} \cdot \frac{N_P}{N_S}$$

$$D' = \frac{V_{IN} - V_{OUT} \cdot \frac{N_P}{N_S}}{V_{IN}}$$

Current-mode forward compensation strategy

- Choose a value for R_{FBT} based on bias current and power dissipation
- Find the modulator transconductance in A/V
- Pick target bandwidth, typically $f_{SW}/10$:

  $\omega_C = 2 \cdot \pi \cdot f_C$
- Find the mid-band gain A_{VM} to achieve target bandwidth

  Adjust R_D, R_P and C_{OUT} as required
- Set ω_{ZEA} equal to 1/10 the target crossover frequency:

  $\omega_{ZEA} = \omega_C/10$
- Set ω_{HF} equal to the ESR zero frequency:

  $\omega_{HF} = \omega_Z$

$$G_m(\text{mod}) = \frac{1}{R_i} \cdot \frac{N_P}{N_S}$$

$$A_{VM} = \frac{\omega_C \cdot C_{OUT}}{G_m(\text{mod})}$$

$$R_D = CTR \cdot \frac{R_P}{\mathrm{A_{VM}}}$$

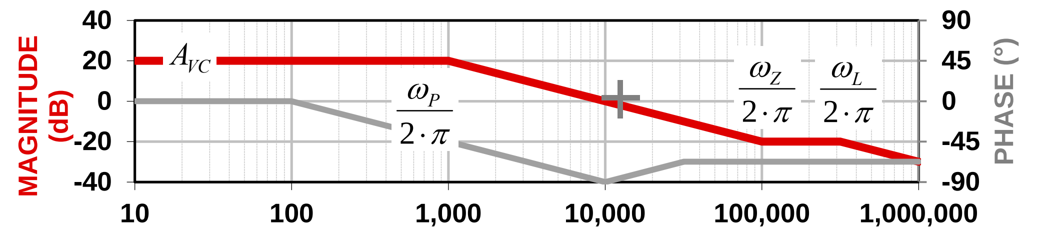
$$C_{COMP} = \frac{1}{R_{FBT} \cdot \omega_{ZEA}}$$

$$C_S = \frac{1}{R_S \cdot \omega_{HF}}$$

Current-mode forward compensation results

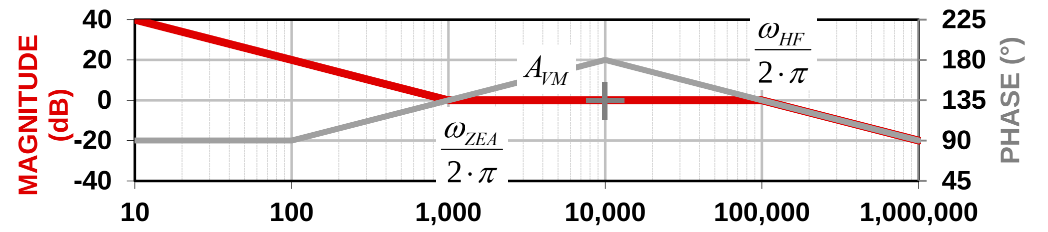
Power stage

$$\frac{\hat{v}_{OUT}}{\hat{v}_C} \approx A_{VC} \cdot \frac{1+\frac{s}{\omega_Z}}{\left(1+\frac{s}{\omega_P}\right)\cdot\left(1+\frac{s}{\omega_L}\right)}$$



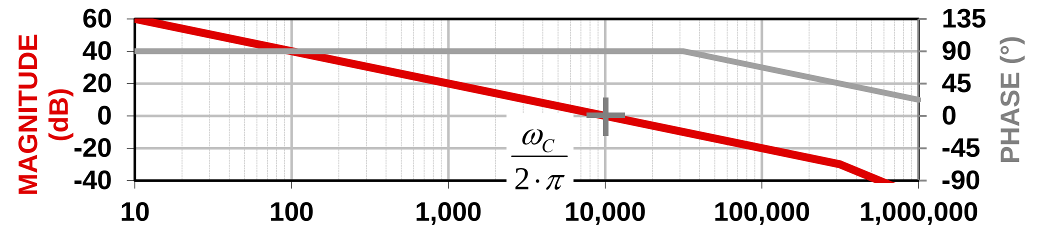
Error amplifier

$$\frac{\hat{v}_C}{\hat{v}'_{OUT}} \approx -A_{VM} \cdot \frac{1+\frac{\omega_{ZEA}}{s}}{1+\frac{s}{\omega_{HF}}}$$



Control loop

$$\frac{\hat{v}_{OUT}}{\hat{v}'_{OUT}} = \frac{\hat{v}_{OUT}}{\hat{v}_C} \cdot \frac{\hat{v}_C}{\hat{v}'_{OUT}}$$



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Mailing Address: Texas Instruments, Post Office Box 655303, Dallas, Texas 75265